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Dimmable Power Factor Corrected LED Driver

NCL30486

The NCL30486 is a power factor corrected flyback controller targeting isolated constant current LED drivers. The controller operates in a quasi−resonant mode to provide high efficiency. Thanks to a novel control method, the device is able to tightly regulate a constant LED current from the primary side. This removes the need for secondary side feedback circuitry, its biasing and for an optocoupler.

The device is highly integrated with a minimum number of external components. A robust suite of safety protection is built in to simplify the design. This device is specifically intended for very compact space efficient designs and supports analog and digital dimming with two dedicated dimming inputs control ideal for Smart LED Lighting applications.

Features

- High Voltage Startup
- Quasi−resonant Peak Current−mode Control Operation
- Primary Side Feedback
- CC / CV Accurate Control V_{in} up to 320 V rms
- Tight LED Constant Current Regulation of ±2% Typical
- Digital Power Factor Correction
- Analog and Digital Dimming
- Cycle by Cycle Peak Current Limit
- Wide Operating V_{CC} Range
- −40 to + 125°C
- Robust Protection Features
  - Brown−Out
  - OVP on V_{CC}
  - Constant Voltage / LED Open Circuit Protection
  - Winding Short Circuit Protection
  - Secondary Diode Short Protection
  - Output Short Circuit Protection
  - Thermal Shutdown
  - Line over Voltage Protection
- This is a Pb−Free Device

Typical Applications

- Integral LED Bulbs
- LED Power Driver Supplies
- LED Light Engines

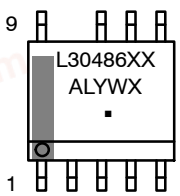
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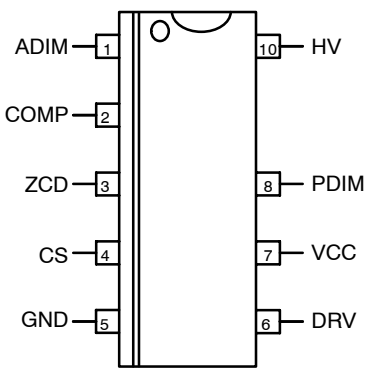
SOIC−9
CASE 751BP

MARKING DIAGRAM



L30486	= Specific Device Code
XX	= Version
A	= Assembly Location
L	= Wafer Lot
YW	= Assembly Start Week
▪	= Pb−Free Package

PIN CONNECTIONS



ORDERING INFORMATION

See detailed ordering and shipping information on page 27 of this data sheet.

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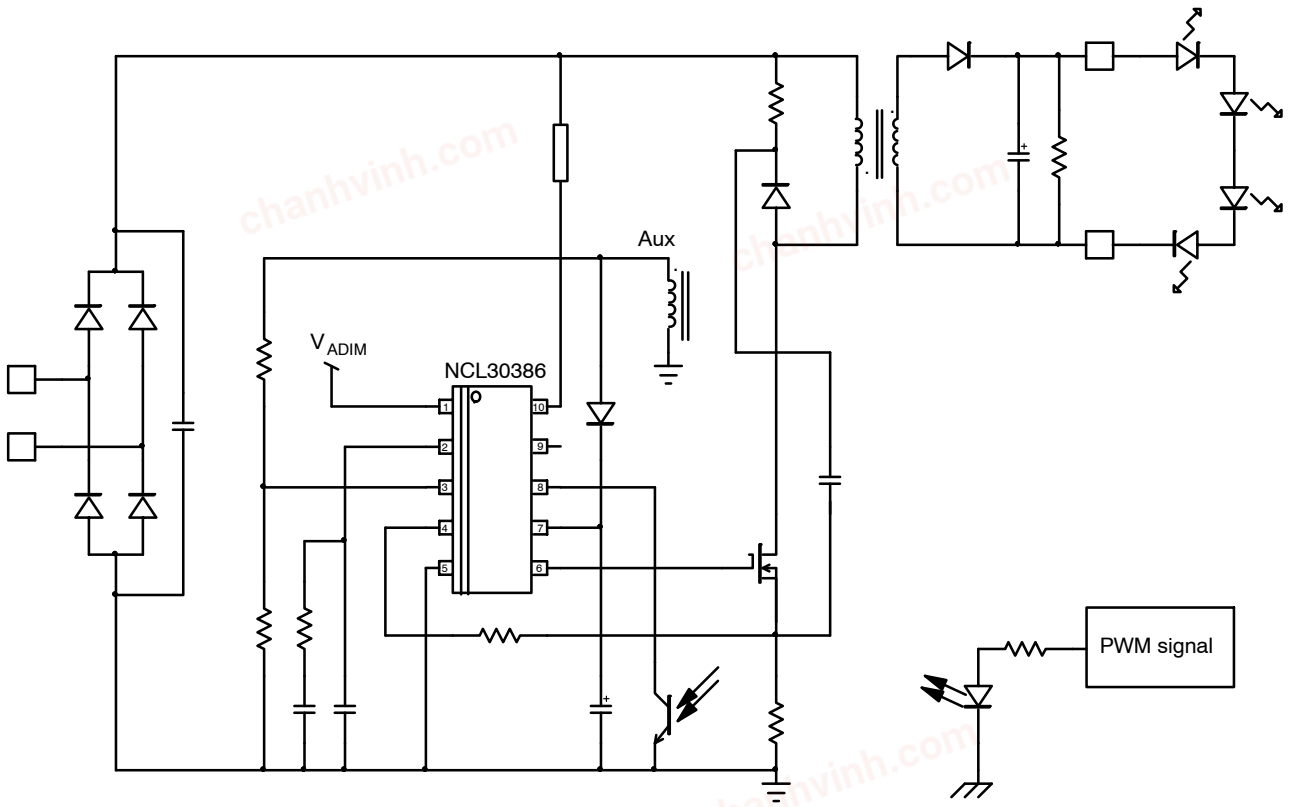


Figure 1. Typical Application Schematic for NCL30486

PIN FUNCTION DESCRIPTION NCL30486

Pin N°	Pin Name	Function	Pin Description
1	ADIM	Analog dimming	This pin is used for analog control of the output current. Applying a voltage varying between $V_{DIM(EN)}$ and V_{DIM100} will dim the output current from 0% to 100%.
2	COMP	OTA output for CV loop	This pin receives a compensation network to stabilize the constant voltage loop
3	ZCD	Zero crossing Detection V_{aux} sensing	This pin connects to the auxiliary winding and is used to detect the core reset event. This pin also senses the auxiliary winding voltage for accurate output voltage control
4	CS	Current sense	This pin monitors the primary peak current.
5	GND	–	The controller ground
6	DRV	Driver output	The driver's output to an external MOSFET
7	VCC	Supplies the controller	This pin is connected to an external auxiliary voltage.
8	PDIM	PWM dimming	This pin is used for PWM dimming control. An optocoupler can be connected directly to the pin if the PWM control signal is from the secondary side
9	NC	creepage	
10	HV	High Voltage sensing	This pin connects after the diode bridge to provide the startup current and internal high voltage sensing function.

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INTERNAL CIRCUIT ARCHITECTURE

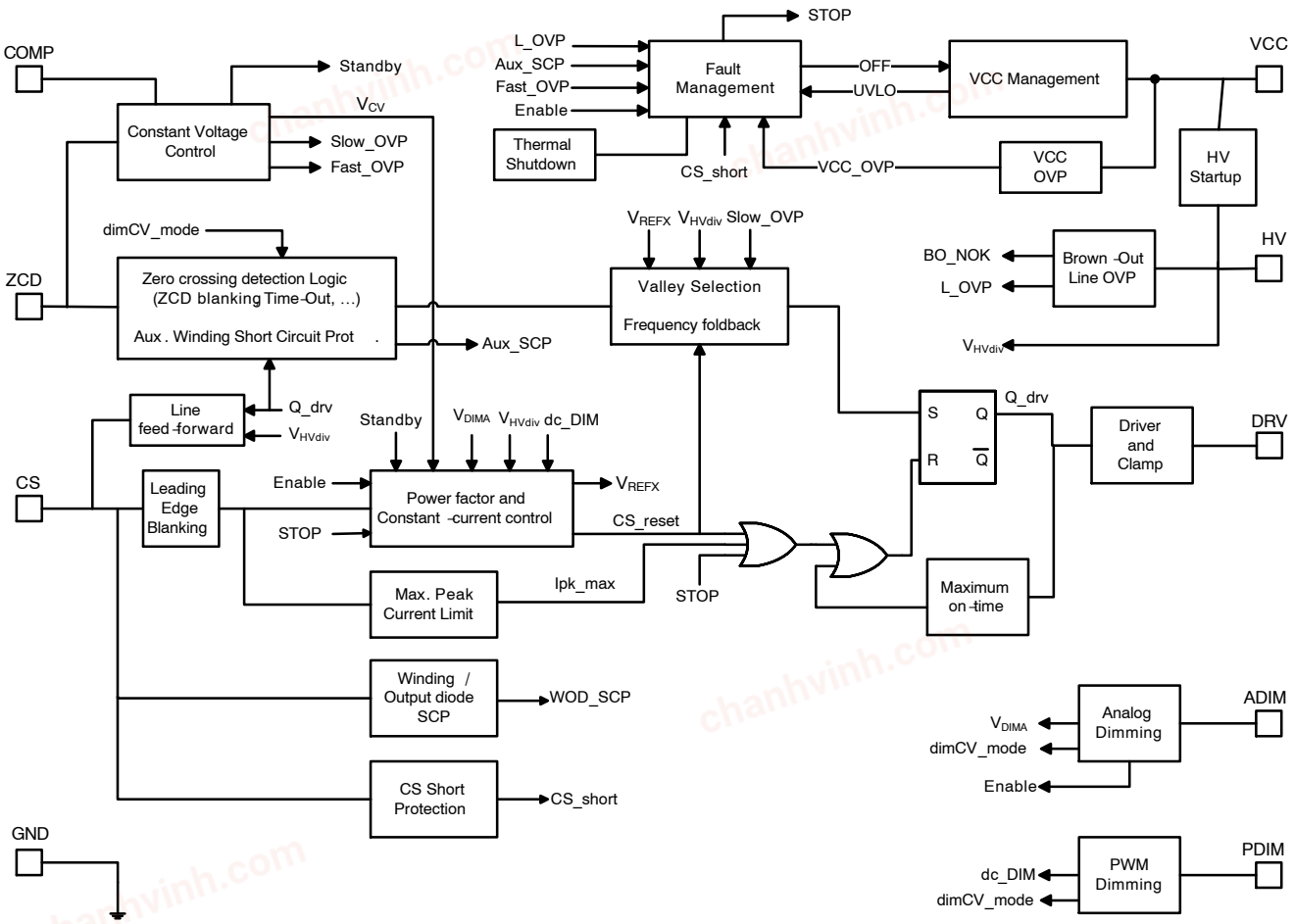


Figure 2. Internal Circuit Architecture NCL30486

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MAXIMUM RATINGS TABLE

Symbol	Rating	Value	Unit
$V_{CC(MAX)}$ $I_{CC(MAX)}$	Maximum Power Supply voltage, VCC pin, continuous voltage Maximum current for VCC pin	−0.3 to 30 Internally limited	V mA
$V_{DRV(MAX)}$ $I_{DRV(MAX)}$	Maximum driver pin voltage, DRV pin, continuous voltage Maximum current for DRV pin	−0.3, V_{DRV} (Note 1) −300, +500	V mA
$V_{HV(MAX)}$ $I_{HV(MAX)}$	Maximum voltage on HV pin Maximum current for HV pin (dc current self−limited if operated within the allowed range)	−0.3, +700 ±20	V mA
V_{MAX} I_{MAX}	Maximum voltage on low power pins (except pins DRV and VCC) Current range for low power pins (except pins DRV and VCC)	−0.3, 5.5 (Note 2) −2, +5	V mA
$R_{\theta J-A}$	Thermal Resistance Junction−to−Air	210	°C/W
$T_{J(MAX)}$	Maximum Junction Temperature	150	°C
	Operating Temperature Range	−40 to +125	°C
	Storage Temperature Range	−60 to +150	°C
	ESD Capability, HBM model except HV pin (Note 3)	4	kV
	ESD Capability, HBM model HV pin	1.5	kV
	ESD Capability, CDM model (Note 3)	1	kV

Stresses exceeding those listed in the Maximum Ratings table may damage the device. If any of these limits are exceeded, device functionality should not be assumed, damage may occur and reliability may be affected.

1. V_{DRV} is the DRV clamp voltage $V_{DRV(high)}$ when V_{CC} is higher than $V_{DRV(high)}$. V_{DRV} is V_{CC} otherwise.
2. This level is low enough to guarantee not to exceed the internal ESD diode and 5.5 V ZENER diode. More positive and negative voltages can be applied if the pin current stays within the −2 mA / 5 mA range.
3. This device series contains ESD protection and exceeds the following tests: Human Body Model 4000 V per Mil−Std−883, Method 3015. Charged Device Model 1000 V per JEDEC Standard JESD22−C101D.
4. This device contains latch−up protection and exceeds 100 mA per JEDEC Standard JESD78.

ELECTRICAL CHARACTERISTICS (Unless otherwise noted: For typical values T_J = 25°C, V_{CC} = 12 V, V_{ZCD} = 0 V, V_{CS} = 0 V) For min/max values T_J = −40°C to +125°C, Max T_J = 150°C, V_{CC} = 12 V)

Parameter	Test Condition	Symbol	Min	Typ	Max	Unit
HIGH VOLTAGE SECTION						
High voltage current source	$V_{CC} = V_{CC(on)} - 200$ mV	$I_{HV(start2)}$	3.9	5.1	6.2	mA
High voltage current source	V_{CC} = 0 V	$I_{HV(start1)}$	−	300	−	μA
V_{CC} level for $I_{HV(start1)}$ to $I_{HV(start2)}$ transition		$V_{CC(TH)}$	−	0.8	−	V
Minimum startup voltage	V_{CC} = 0 V	$V_{HV(MIN)}$	−	17	−	V
HV source leakage current	V_{HV} = 450 V	$I_{HV(leak)}$	−	4.5	10	μA
Maximum input voltage (rms) for correct operation of the PFC loop		$V_{HV(OL)}$	320	−	−	V rms
SUPPLY SECTION						
Supply Voltage Startup Threshold Minimum Operating Voltage Hysteresis $V_{CC(on)} - V_{CC(off)}$ Internal logic reset	 V_{CC} increasing V_{CC} decreasing V_{CC} decreasing	 $V_{CC(on)}$ $V_{CC(off)}$ $V_{CC(HYS)}$ $V_{CC(reset)}$	 16 9.3 7.6 4	 18 10.2 − 5	 20 10.7 − 6	V
Over Voltage Protection VCC OVP threshold		$V_{CC(OVP)}$	25	26.5	28	V
$V_{CC(off)}$ noise filter (Note 5) $V_{CC(reset)}$ noise filter (Note 5)		$t_{VCC(off)}$ $t_{VCC(reset)}$	− −	5 20	− −	μs
Supply Current Device Disabled/Fault Device Enabled/No output load on pin 5 Device Switching (F_{sw} = 65 kHz) Device switching (F_{sw} = 700 Hz)	 $V_{CC} > V_{CC(off)}$ F_{sw} = 65 kHz C_{DRV} = 470 pF, F_{sw} = 65 kHz $V_{COMP} \leq$ 0.9 V	 I_{CC1} I_{CC2} I_{CC3} I_{CC4}	 1.2 − − −	 1.35 3.0 3.5 1.7	 1.6 3.5 4.0 1.88	mA

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ELECTRICAL CHARACTERISTICS (Unless otherwise noted: For typical values T_J = 25°C, V_{CC} = 12 V, V_{ZCD} = 0 V, V_{CS} = 0 V) For min/max values T_J = −40°C to +125°C, Max T_J = 150°C, V_{CC} = 12 V) (continued)

Parameter	Test Condition	Symbol	Min	Typ	Max	Unit
CURRENT SENSE						
Maximum Internal current limit		V_{ILIM}	1.33	1.40	1.47	V
Leading Edge Blanking Duration for V_{ILIM}		t_{LEB}	283	345	407	ns
Propagation delay from current detection to gate off−state		t_{ILIM}	–	100	150	ns
Maximum on−time (option 1)		$t_{on(MAX)}$	29	39	49	μs
Maximum on−time (option 2)		$t_{on(MAX)}$	16	20	24	μs
Threshold for immediate fault protection activation (140% of V_{ILIM})		$V_{CS(stop)}$	1.9	2.0	2.1	V
Leading Edge Blanking Duration for $V_{CS(stop)}$		t_{BCS}	–	170	–	ns
Current source for CS to GND short detection		$I_{CS(short)}$	400	500	600	μA
Current sense threshold for CS to GND short detection	V_{CS} rising	$V_{CS(low)}$	20	60	90	mV
GATE DRIVE						
Drive Resistance DRV Sink DRV Source		 R_{SNK} R_{SRC}	 – –	 13 30	 – –	Ω
Drive current capability DRV Sink (Note GBD) DRV Source (Note GBD)		 I_{SNK} I_{SRC}	 – –	 500 300	 – –	mA
Rise Time (10% to 90%)	C_{DRV} = 470 pF	t_r	–	30	–	ns
Fall Time (90 %to 10%)	C_{DRV} = 470 pF	t_f	–	20	–	ns
DRV Low Voltage	$V_{CC} = V_{CC(off)}$+0.2 V C_{DRV} = 470 pF, R_{DRV} = 33 kΩ	$V_{DRV(low)}$	8	–	–	V
DRV High Voltage	$V_{CC} = V_{CC(MAX)}$ C_{DRV} = 470 pF, R_{DRV} = 33 kΩ	$V_{DRV(high)}$	10	12	14	V
ZERO VOLTAGE DETECTION CIRCUIT						
Upper ZCD threshold voltage	V_{ZCD} rising	$V_{ZCD(rising)}$	–	90	150	mV
Lower ZCD threshold voltage	V_{ZCD} falling	$V_{ZCD(falling)}$	35	55	–	mV
Threshold to force V_{REFX} maximum during startup		$V_{ZCD(start)}$	–	0.7	–	V
ZCD hysteresis		$V_{ZCD(HYS)}$	15	–	–	mV
Propagation Delay from valley detection to DRV high (no t_{LEB4})	V_{ZCD} decreasing	$t_{ZCD(DEM)}$	–	–	150	ns
Additional delay from valley lockout output to DRV latch set (prog option)		t_{LEB4}	125	250	375	ns
Equivalent time constant for ZCD input (GBD)		t_{PAR}	–	20	–	ns
Blanking delay after on−time (option 1)	V_{REFX} > 0.35 V	$t_{ZCD(blank1)}$	1.1	1.5	1.9	μs
Blanking delay after on−time (option 2)	V_{REFX} > 0.35 V	$t_{ZCD(blank1)}$	0.75	1.0	1.25	μs
Blanking Delay at light load (option 1)	V_{REFX} < 0.25 V	$t_{ZCD(blank2)}$	0.6	0.8	1.0	μs
Blanking Delay at light load (option 2)	V_{REFX} < 0.25 V	$t_{ZCD(blank2)}$	0.45	0.6	0.75	μs
Timeout after last DEMAG transition		t_{TIMO}	5	6.5	8	μs
Pulling−down resistor	$V_{ZCD} = V_{ZCD(falling)}$	$R_{ZCD(pd)}$	–	200	–	kΩ
ZCD pin current source for forcing CV mode when minimum dimming	V_{ADIM} = 0.5 V	I_{ZCDdim}	145	170	195	μA

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ELECTRICAL CHARACTERISTICS (Unless otherwise noted: For typical values T_J = 25°C, V_{CC} = 12 V, V_{ZCD} = 0 V, V_{CS} = 0 V) For min/max values T_J = −40°C to +125°C, Max T_J = 150°C, V_{CC} = 12 V) (continued)

Parameter	Test Condition	Symbol	Min	Typ	Max	Unit
CONSTANT CURRENT CONTROL						
Reference Voltage	T_j = 25°C – 85°C	$V_{REF/3}$	327.9	334.2	341.2	mV
Reference Voltage	T_j = −40°C to 125°C	$V_{REF/3}$	324	334.2	346	mV
10% Reference Voltage	T_j = 25°C – 85°C	$V_{REF10/3}$	30	33.33	36.66	mV
10% Reference Voltage	T_j = −40°C to 125°C	$V_{REF10/3}$	27.33	33.33	39.33	mV
5% Reference Voltage	T_j = 25°C – 85°C	$V_{REF05/3}$	14.17	17	19.17	mV
5% Reference Voltage	T_j = −40°C to 125°C	$V_{REF05/3}$	13.34	17	20	mV
Current sense lower threshold for detection of the leakage inductance reset time	V_{CS} falling	$V_{CS(low)}$	20	50	100	mV
Blanking time for leakage inductance reset detection		$t_{CS(low)}$	–	120	–	ns
POWER FACTOR CORRECTION						
Clamping value for $V_{REF(PFC)}$	T_J = 0°C to 125°C	$V_{REF(PFC)CLP}$	2.06	2.2	2.34	V
Line range detector for PFC loop	V_{HV} increases	$V_{HL(PFC)}$	–	240	–	Vdc
Line range detector for PFC loop	V_{HV} decreases	$V_{LL(PFC)}$	–	230	–	Vdc
CONSTANT VOLTAGE SECTION						
Internal voltage reference for constant voltage regulation		$V_{REF(CV)}$	3.41	3.52	3.63	V
CV Error amplifier Gain		G_{EA}	40	50	60	μS
Error amplifier current capability	V_{REFX} = V_{REF} (no dimming)	I_{EA}	–	±60	–	μA
COMP pin lower clamp voltage		$V_{CV(clampL)}$	–	0.6	–	V
COMP pin higher clamp voltage	T_J = 0°C to 125°C	$V_{CV(clampH)}$	4.05	4.12	4.25	V
COMP pin higher clamp voltage	T_J = −40°C to 125°C	$V_{CV(clampH)}$	4.01	4.12	4.25	V
Internal ZCD voltage below which the CV OTA is boosted	$V_{REF(CV)}$ * 85%	$V_{boost(CV)}$	2.796	2.975	3.154	V
Threshold for releasing the CV boost	$V_{REF(CV)}$ * 90%	$V_{boost(CV)RST}$	2.96	3.15	3.34	V
Internal ZCD voltage below which the CV OTA is boosted (opt.2)	$V_{REF(CV)}$ * 80%	$V_{boost(CV)2}$	2.632	2.8	2.968	V
Error amplifier current capability during boost phase		$I_{EAboost}$	–	±140	–	μA
ZCD OVP 1st level (slow OVP) option 1	$V_{REF(CV)}$ * 115%	V_{OVP1}	3.783	4.025	4.267	V
ZCD OVP 1st level (slow OVP) option 2	$V_{REF(CV)}$ * 120%	V_{OVP1}	3.948	4.2	4.452	V
ZCD voltage at which slow OVP is exit (option 1)	$V_{REF(CV)}$ * 105%	$V_{OVP1rst}$	–	3.675	–	V
ZCD voltage at which slow OVP is exit (option 2)	$V_{REF(CV)}$ * 110%	$V_{OVP1rst}$	–	3.85	–	V
Switching period during slow OVP		$T_{sw(OVP1)}$	–	1.5	–	ms
ZCD fast OVP option 2	$V_{ref(CV)}$ * 130% + 150 mV	V_{OVP2}	–	4.7	–	V
ZCD fast OVP option 1	$V_{ref(CV)}$ * 125% + 150 mV	V_{OVP2}	4.253	4.525	4.797	V
Number of switching cycles before fast OVP confirmation		T_{OVP2_CNT}	–	4	–	
Duration for disabling DRV pulses during ZCD fast OVP		$T_{recovery}$	–	4	–	s
COMP pin internal pullup resistor (prog option)		R_{pullup}	–	15	–	kΩ
LINE FEED FORWARD						
V_{HV} to $I_{CS(offset)}$ conversion ratio		K_{LFF}	0.189	0.21	0.231	μA/V
Offset current maximum value	V_{HV} > (450 V or 500 V)	$I_{offset(MAX)}$	76	95	114	μA
Line feed−forward current	DRV high, V_{HV} = 200 V	I_{FF}	35	40	45	μA

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ELECTRICAL CHARACTERISTICS (Unless otherwise noted: For typical values T_J = 25°C, V_{CC} = 12 V, V_{ZCD} = 0 V, V_{CS} = 0 V) For min/max values T_J = −40°C to +125°C, Max T_J = 150°C, V_{CC} = 12 V) (continued)

Parameter	Test Condition	Symbol	Min	Typ	Max	Unit
VALLEY LOCKOUT SECTION						
Threshold for line range detection V_{HV} increasing (1st to 2nd valley transition for V_{REFX} > 80% V_{REF}) (prog. option: 1st to 3rd valley transition)	V_{HV} increases	V_{HL}	228	240	252	V
Threshold for line range detection V_{HV} decreasing (2nd to 1st valley transition for V_{REFX} > 80% V_{REF}) (prog. option: 3rd to 1st valley transition)	V_{HV} decreases	V_{LL}	218	230	242	V
Blanking time for line range detection		$t_{HL(blank)}$	15	25	35	ms
Valley thresholds						V
1st to 2nd valley transition at LL and 2nd to 3rd valley HL, V_{REF} decr. (prog. option: 3rd to 4th valley HL)	V_{REF} decreases	$V_{VLY1-2/2-3}$	–	0.80	–	
2nd to 1st valley transition at LL and 3rd to 2nd valley HL, V_{REF} incr. (prog. option: 4th to 3rd valley HL)	V_{REF} increases	$V_{VLY2-1/3-2}$	–	0.90	–	
2nd to 3rd valley transition at LL and 3rd to 4th valley HL, V_{REF} decr. (prog. option: 4th to 5th valley HL)	V_{REF} decreases	$V_{VLY2-3/3-4}$	–	0.65	–	
3rd to 2nd valley transition at LL and 4th to 3rd valley HL, V_{REF} incr. (prog. option: 5th to 4th valley HL)	V_{REF} increases	$V_{VLY3-2/4-3}$	–	0.75	–	
3rd to 4th valley transition at LL and 4th to 5th valley HL, V_{REF} decr. (prog. option: 5th to 6th valley HL)	V_{REF} decreases	$V_{VLY3-4/4-5}$	–	0.50	–	
4th to 3th valley transition at LL and 5th to 4th valley HL, V_{REF} incr. (prog. option: 6th to 5th valley HL)	V_{REF} increases	$V_{VLY4-3/5-4}$	–	0.60	–	
4th to 5th valley transition at LL and 5th to 6th valley HL, V_{REF} decr. (prog. option: 6th to 7th valley HL)	V_{REF} decreases	$V_{VLY4-5/5-6}$	–	0.35	–	
5th to 4th valley transition at LL and 6th to 5th valley HL, V_{REF} incr. (prog. option: 7th to 6th valley HL)	V_{REF} increases	$V_{VLY5-4/6-5}$	–	0.45	–	
V_{REF} value at which the FF mode is activated	V_{REF} decreases	$V_{FFstart}$	–	0.25	–	V
V_{REF} value at which the FF mode is removed	V_{REF} increases	V_{FFstop}	–	0.35	–	V
FREQUENCY FOLDBACK						
Added dead time	V_{REFX} = 0.25 V	t_{FF1LL}	0.8	1.0	1.2	μs
Added dead time	V_{REFX} = 0.08 V	t_{FFchg}	–	40	–	μs
Dead−time clamp (option 1)	V_{REFX} < 3 mV	t_{FFend1}	–	675	–	μs
Dead−time clamp (option 2)	V_{REFX} < 11.2 mV	t_{FFend2}	–	250	–	μs
DIMMING SECTION						
DIM pin voltage for zero output current (OFF voltage)		$V_{ADIM(EN)}$	0.475	0.5	0.525	V
ADIM pin voltage for 1% reference voltage		$V_{ADIM(MIN)}$	0.668	0.7	0.732	V
Minimum dimming level (option 1)		$K_{DIM(MIN)1}$	–	0	–	%
Minimum dimming level (option 2)		$K_{DIM(MIN)2}$	–	1	–	%
Minimum dimming level (option 3)		$K_{DIM(MIN)3}$	–	5	–	%
Minimum dimming level (option 4)		$K_{DIM(MIN)4}$	–	8	–	%
ADIM pin voltage for maximum output current (V_{REFX} = 1 V)		$V_{ADIM100}$	–	3.0	3.1	V
Dimming range		$V_{ADIM(range)}$	–	2.3	–	V
Clamping voltage for DIM pin		$V_{ADIM(CLP)}$	–	6.8	–	V
Dimming pin pull−up current source		$I_{ADIM(pullup)1}$	8	10	12	μA
Current Comparator threshold for PDIM	I_{PDIM} rising	$I_{PDIM(THR)}$	60	70	80	μA
Current Comparator threshold for PDIM	I_{PDIM} falling	$I_{PDIM(THD)}$	131	153	175	μA
Cascode current limit for PDIM		$I_{PDIM(LIM)}$	–	1080	–	μA
PDIM pin voltage		V_{PDIM}	–	3	–	V
Maximum period of the PWM dimming signal			–	6	–	ms
Minimum on−time for PWM signal applied on PDIM			–	8	–	μs

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ELECTRICAL CHARACTERISTICS (Unless otherwise noted: For typical values T_J = 25°C, V_{CC} = 12 V, V_{ZCD} = 0 V, V_{CS} = 0 V) For min/max values T_J = −40°C to +125°C, Max T_J = 150°C, V_{CC} = 12 V) (continued)

Parameter	Test Condition	Symbol	Min	Typ	Max	Unit
FAULT PROTECTION						
Thermal Shutdown (Note 5)	Device switching (F_{SW} around 65 kHz)	T_{SHDN}	130	150	170	°C
Thermal Shutdown Hysteresis		$T_{SHDN(HYS)}$	–	20	–	°C
Threshold voltage for output short circuit or aux. winding short circuit detection		$V_{ZCD(short)}$	0.6	0.65	0.7	V
Short circuit detection Timer	$V_{ZCD} < V_{ZCD(short)}$	t_{OVLD}	70	90	110	ms
Auto−recovery Timer		$t_{recovery}$	3	4	5	s
Line OVP threshold	V_{HV} increasing	$V_{HV(OVP)}$	457	469	485	Vdc
HV pin voltage at which Line OVP is reset	V_{HV} decreasing	$V_{HV(OVP)RST}$	430	443	465	Vdc
Blanking time for line OVP reset		$T_{LOVP(blank)}$	15	25	35	ms
BROWN−OUT AND LINE SENSING						
Brown−Out ON level (IC start pulsing)	V_{HV} increasing	$V_{HVBO(on)}$	101.5	108	114.5	Vdc
Brown−Out ON level (IC start pulsing) option 2	V_{HV} increasing	$V_{HVBO(on)2}$	129.7	138	146.3	Vdc
Brown−Out OFF level (IC stops pulsing)	V_{HV} decreasing	$V_{HVBO(off)}$	92	98	104	Vdc
Brown−Out OFF level (IC stops pulsing) option 2	V_{HV} decreasing	$V_{HVBO(off)2}$	121	129	137	Vdc
HV pin voltage above which the sampling of ZCD is enabled low line	V_{HV} decreasing, low line	$V_{sampENLL}$	–	55	–	V
HV pin voltage above which the sampling of ZCD is enabled highline	V_{HV} decreasing, highline	$V_{sampENHL}$	–	105	–	V
ZCD sampling enable comparator hysteresis	V_{HV} increasing	$V_{sampHYS}$	–	5	–	V
BO comparators delay		$t_{BO(delay)}$	–	30	–	μs
Brown−Out blanking time		$t_{BO(blank)}$	15	25	35	ms

Product parametric performance is indicated in the Electrical Characteristics for the listed test conditions, unless otherwise noted. Product performance may not be indicated by the Electrical Characteristics if operated under different conditions.

5. Guaranteed by design.

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TYPICAL CHARACTERISTICS

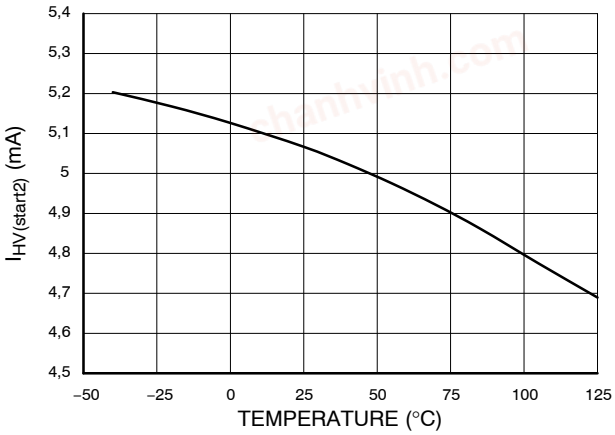


Figure 3. $I_{HV(start2)}$ vs. Temperature

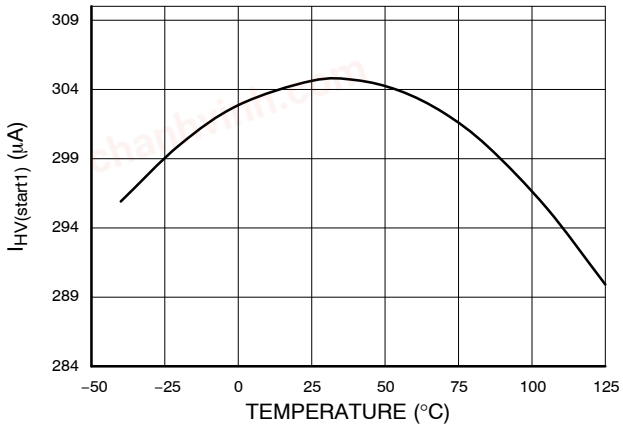


Figure 4. $I_{HV(start1)}$ vs. Temperature

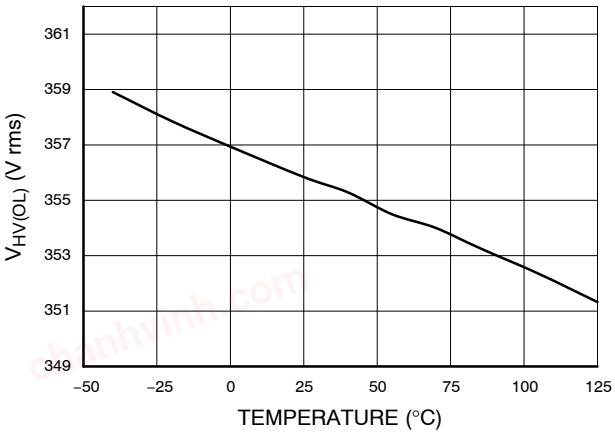


Figure 5. $V_{HV(OL)}$ vs. Temperature

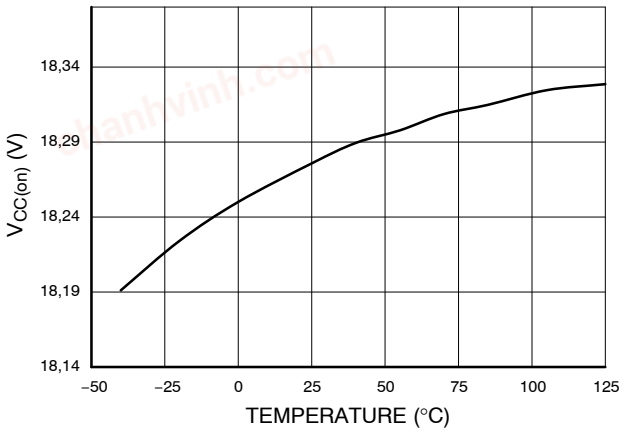


Figure 6. $V_{CC(on)}$ vs. Temperature

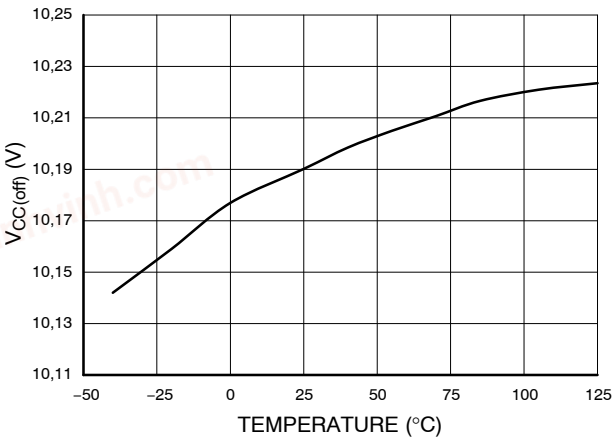


Figure 7. $V_{CC(off)}$ vs. Temperature

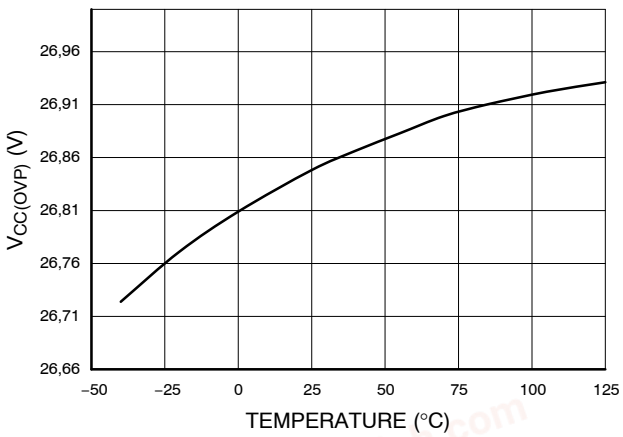


Figure 8. $V_{CC(OVP)}$ vs. Temperature

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TYPICAL CHARACTERISTICS (continued)

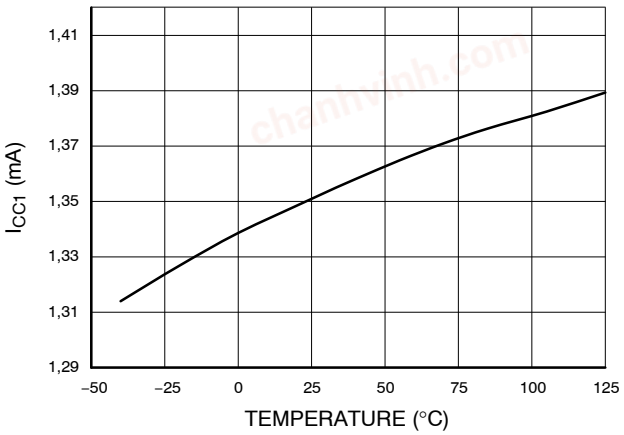


Figure 9. I_{CC1} vs. Temperature

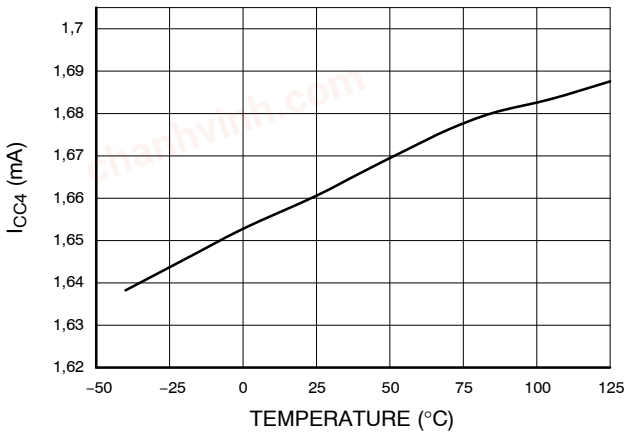


Figure 10. I_{CC4} vs. Temperature

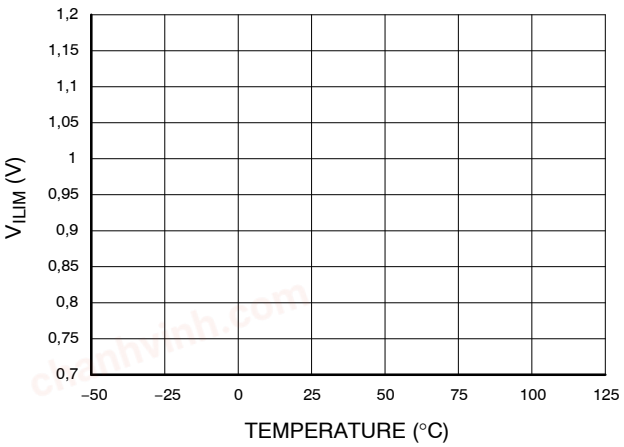


Figure 11. V_{ILIM} vs. Temperature

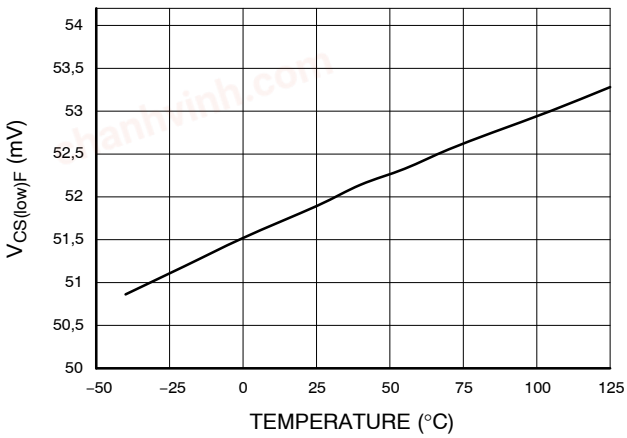


Figure 12. $V_{CS(low)F}$ vs. Temperature

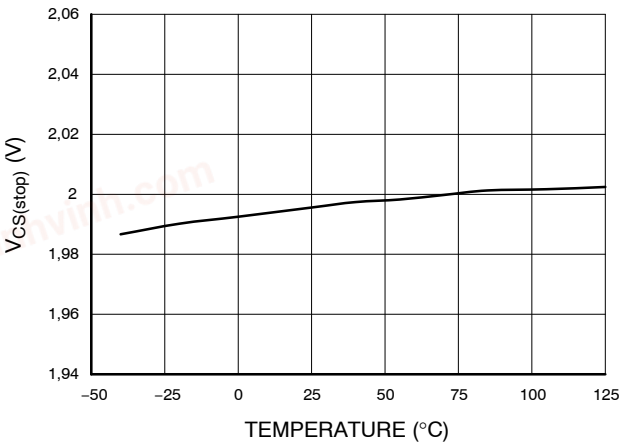


Figure 13. $V_{CS(stop)}$ vs. Temperature

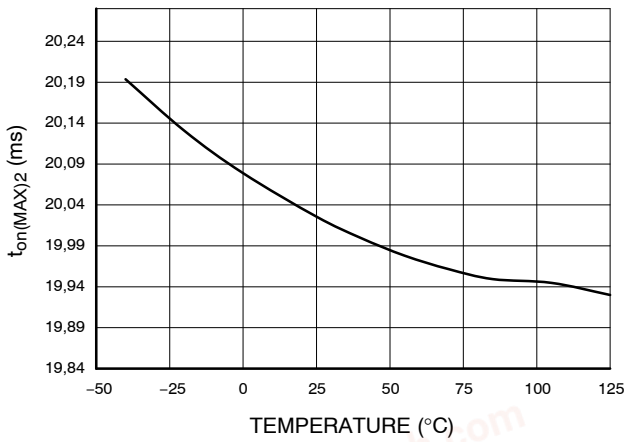


Figure 14. $t_{on(MAX)2}$ vs. Temperature

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TYPICAL CHARACTERISTICS (continued)

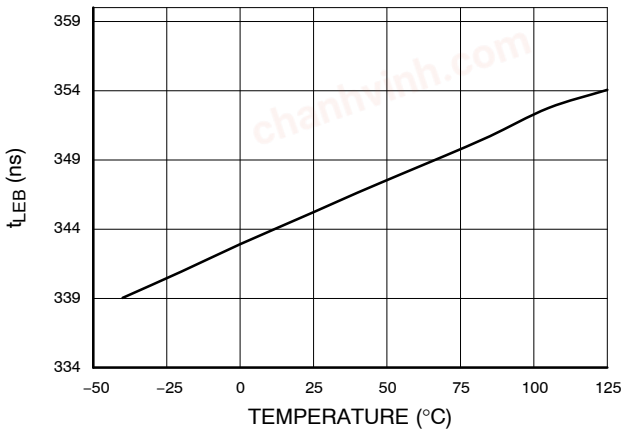


Figure 15. t_{LEB} vs. Temperature

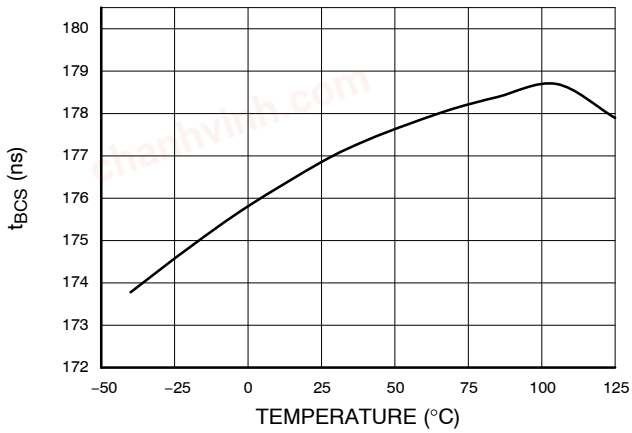


Figure 16. t_{BCS} vs. Temperature

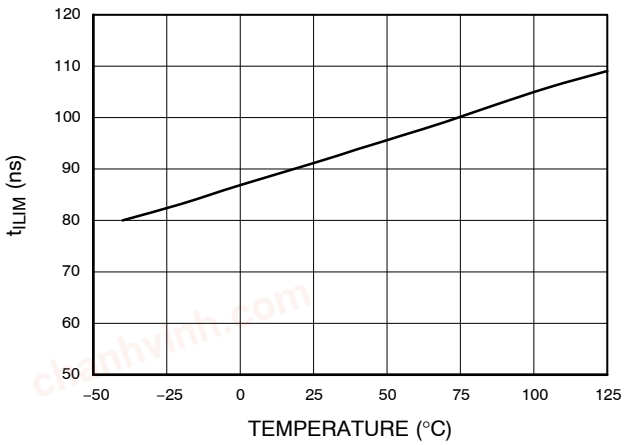


Figure 17. t_{ILIM} vs. Temperature

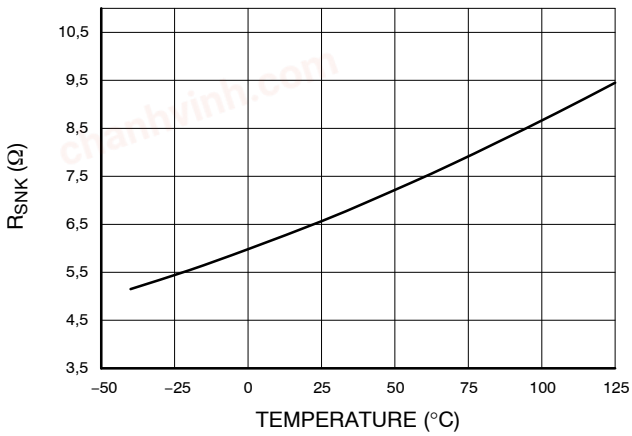


Figure 18. R_{SNK} vs. Temperature

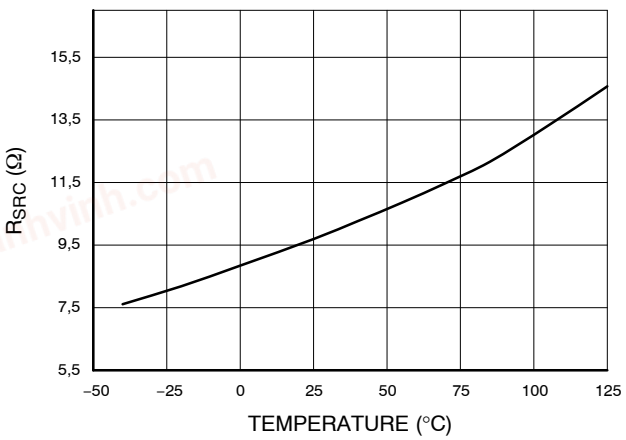


Figure 19. R_{SRC} vs. Temperature

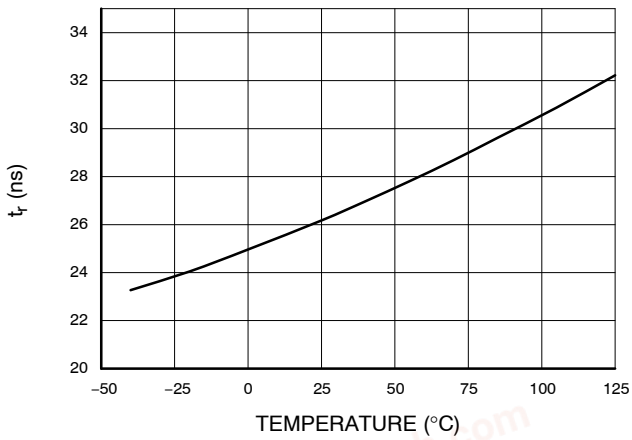


Figure 20. t_r vs. Temperature

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TYPICAL CHARACTERISTICS (continued)

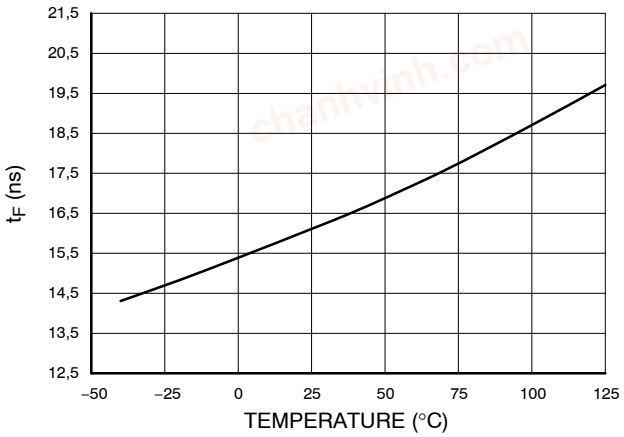


Figure 21. t_f vs. Temperature

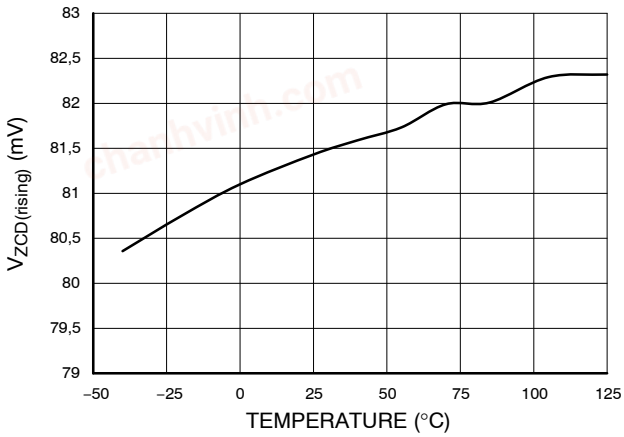


Figure 22. $V_{ZCD(rising)}$ vs. Temperature

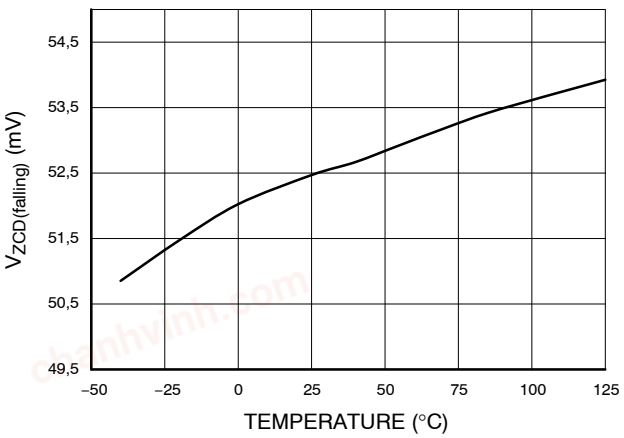


Figure 23. $V_{ZCD(falling)}$ vs. Temperature

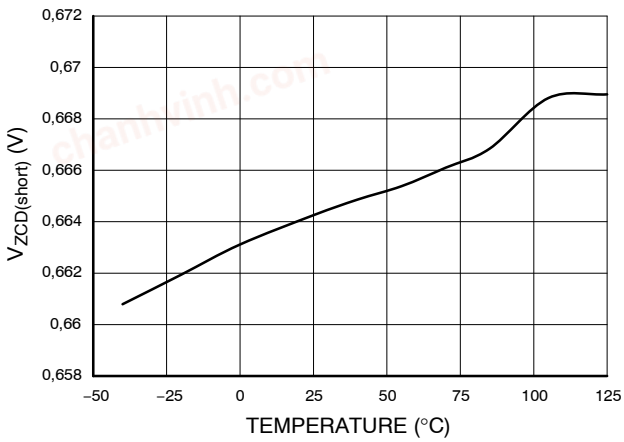


Figure 24. $V_{ZCD(short)}$ vs. Temperature

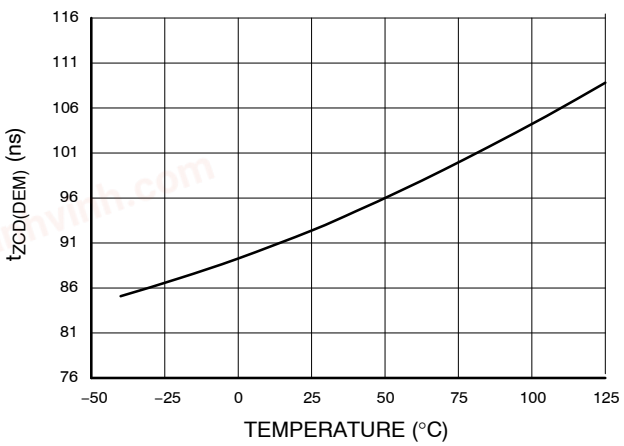


Figure 25. $t_{ZCD(dem)}$ vs. Temperature

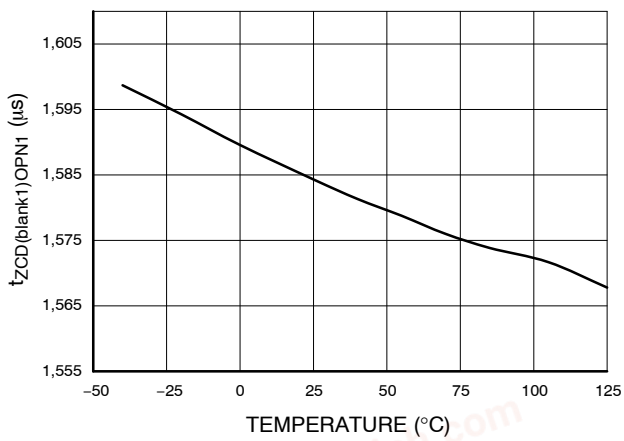


Figure 26. $t_{ZCD(blank1)OPN1}$ vs. Temperature

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TYPICAL CHARACTERISTICS (continued)

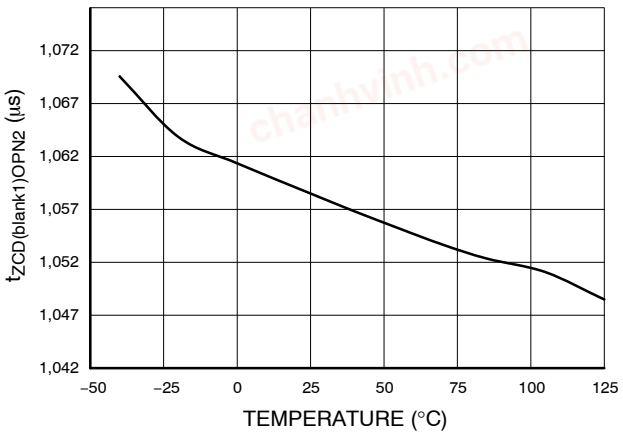


Figure 27. $t_{ZCD(blank1)OPN2}$ vs. Temperature

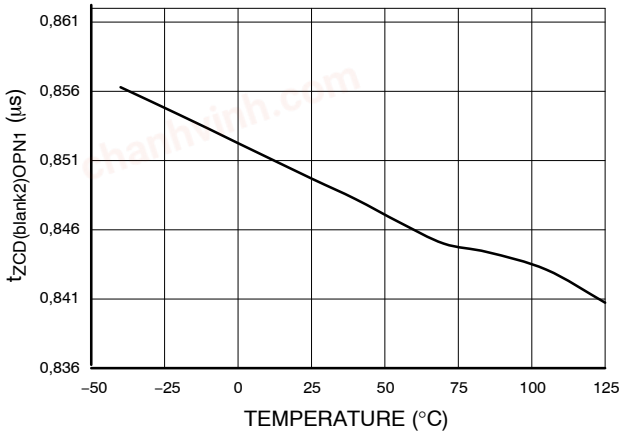


Figure 28. $t_{ZCD(blank2)OPN1}$ vs. Temperature

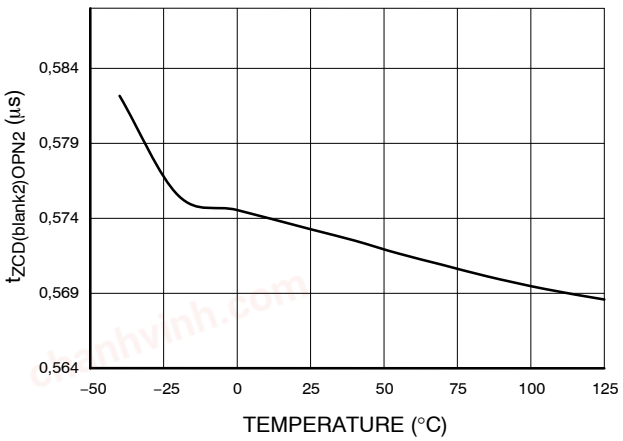


Figure 29. $t_{ZCD(blank2)}$OPN2 vs. Temperature

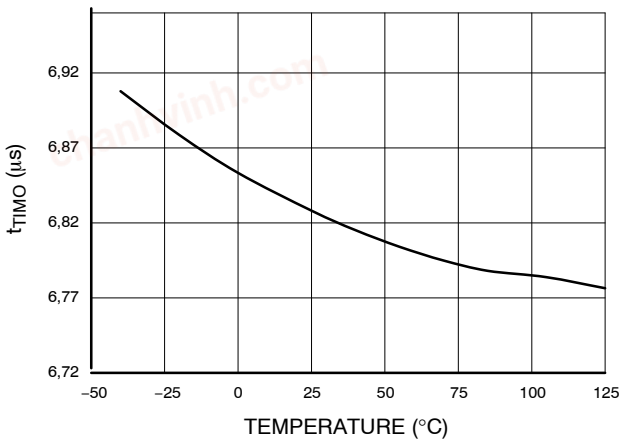


Figure 30. t_{TIMO} vs. Temperature

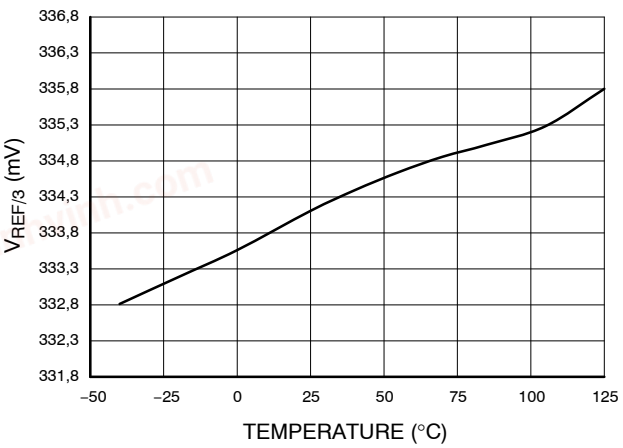


Figure 31. $V_{REF/3}$ vs. Temperature

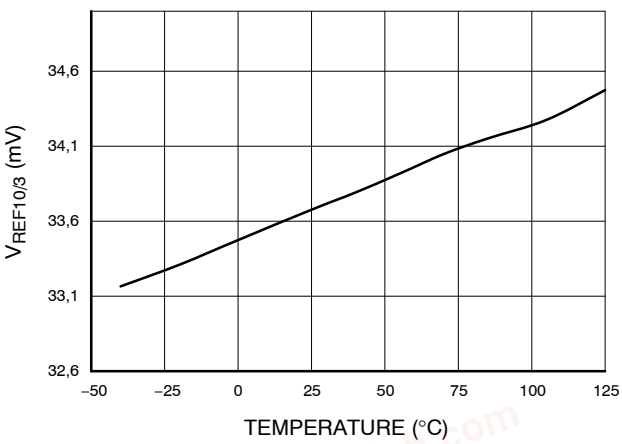


Figure 32. $V_{REF10/3}$ vs. Temperature

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TYPICAL CHARACTERISTICS (continued)

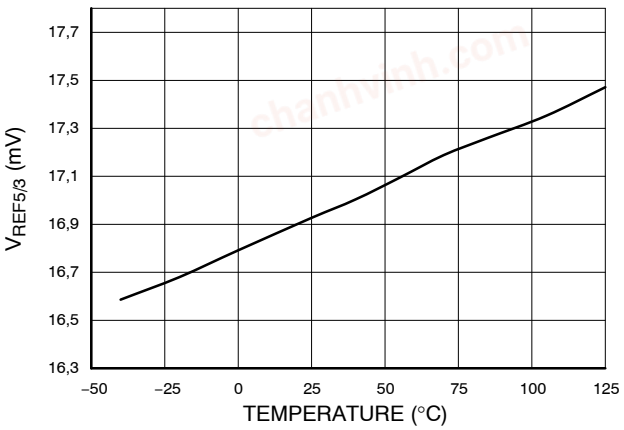


Figure 33. $V_{REF5/3}$ vs. Temperature

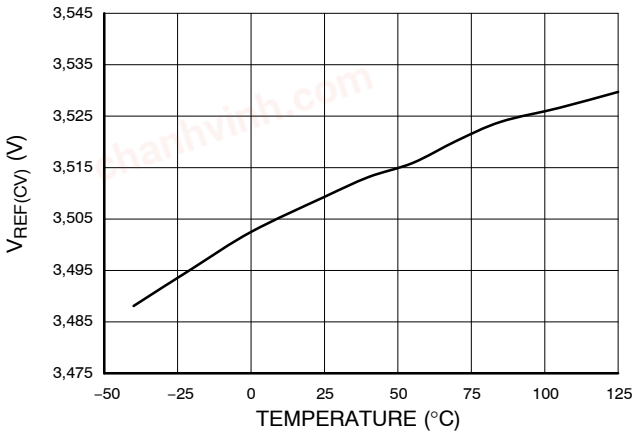


Figure 34. $V_{REF(CV)}$ vs. Temperature

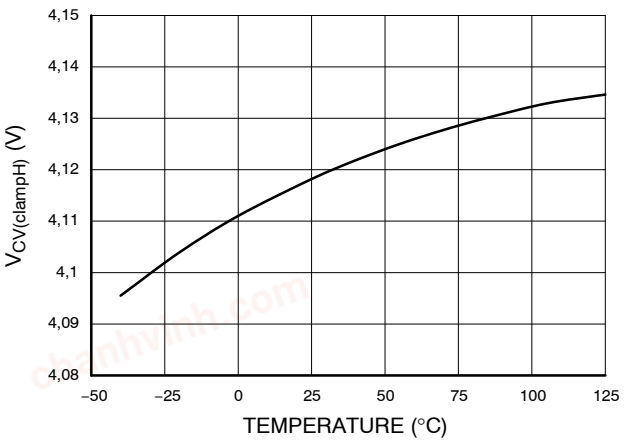


Figure 35. $V_{CV(clampH)}$ vs. Temperature

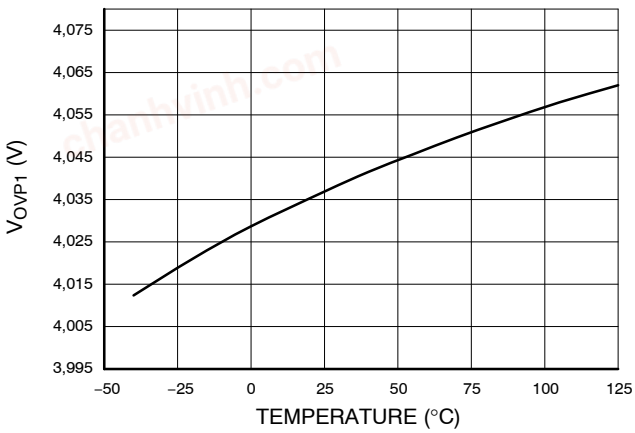


Figure 36. V_{OVP1} vs. Temperature

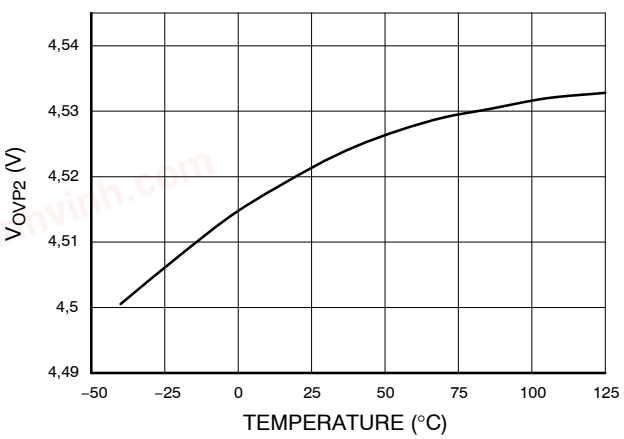


Figure 37. V_{OVP2} vs. Temperature

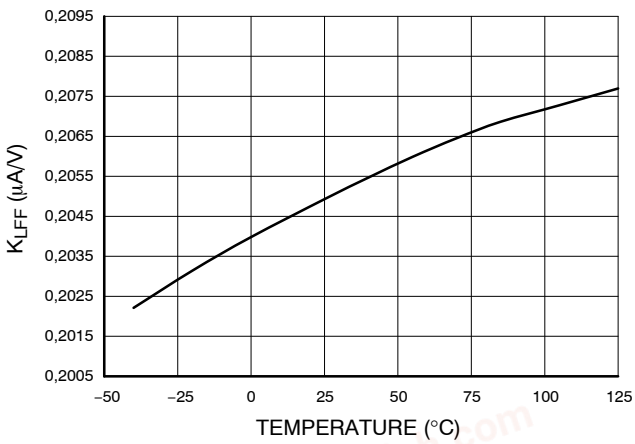


Figure 38. K_{LFF} vs. Temperature

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TYPICAL CHARACTERISTICS (continued)

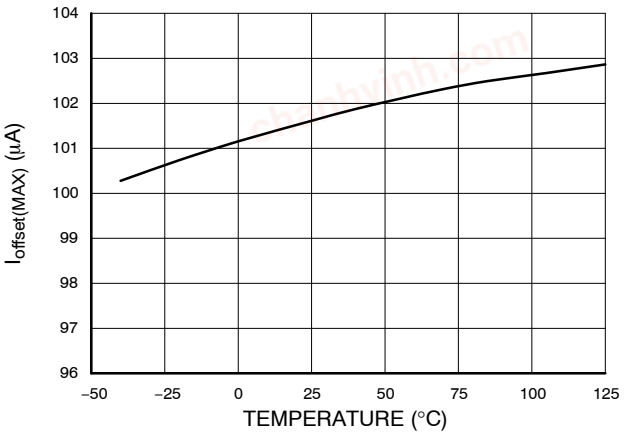


Figure 39. $I_{offset(MAX)}$ vs. Temperature

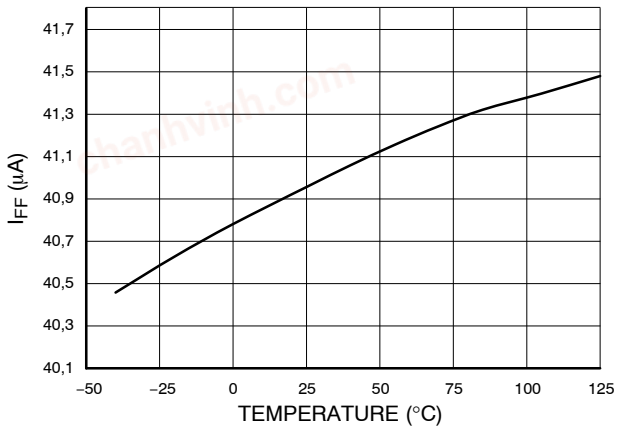


Figure 40. I_{FF} vs. Temperature

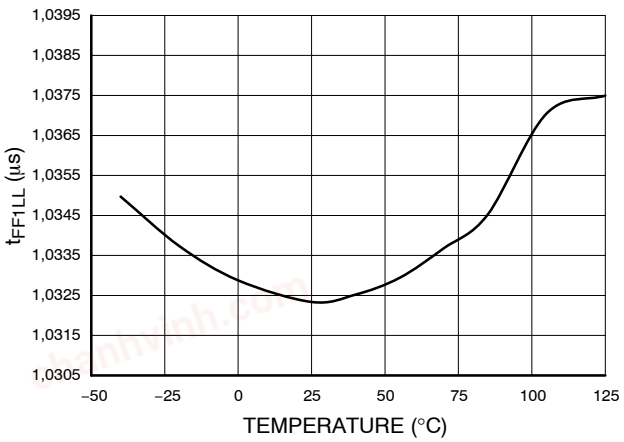


Figure 41. t_{FF1LL} vs. Temperature

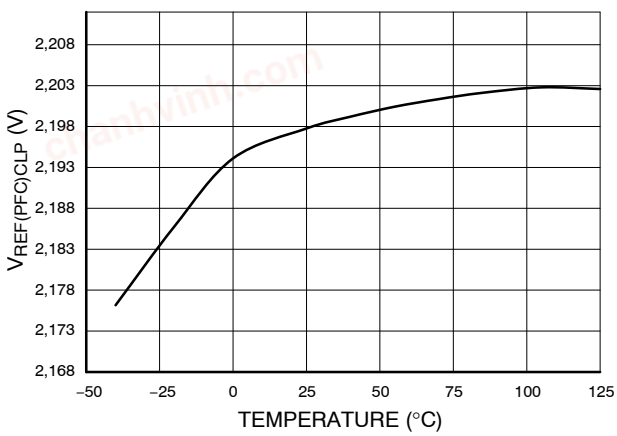


Figure 42. $V_{REF(PFC)CLP}$ vs. Temperature

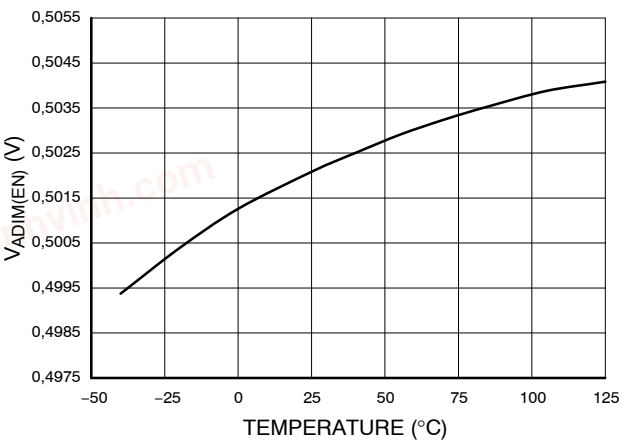


Figure 43. $V_{ADIM(EN)}$ vs. Temperature

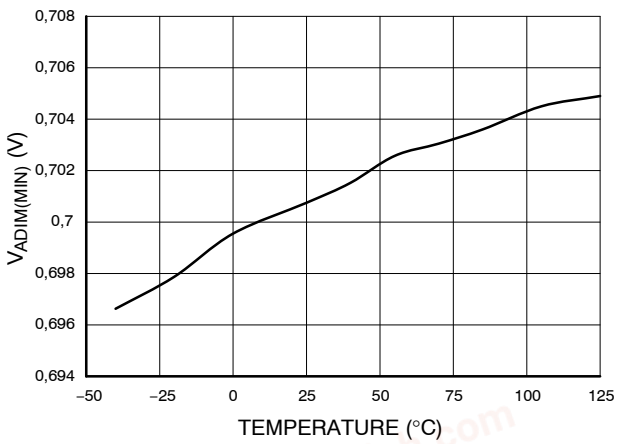


Figure 44. $V_{ADIM(MIN)}$ vs. Temperature

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TYPICAL CHARACTERISTICS (continued)

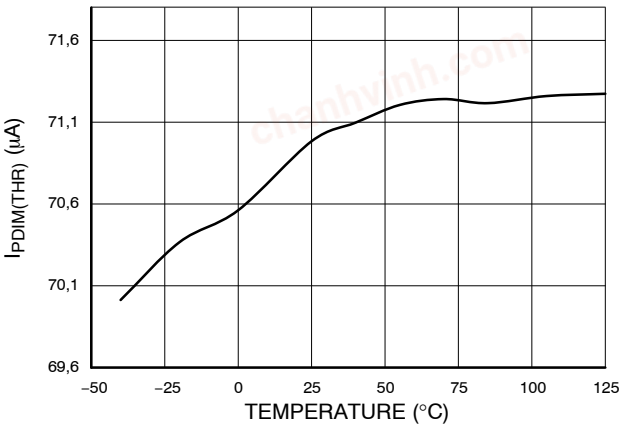


Figure 45. $I_{PDIM(THR)}$ vs. Temperature

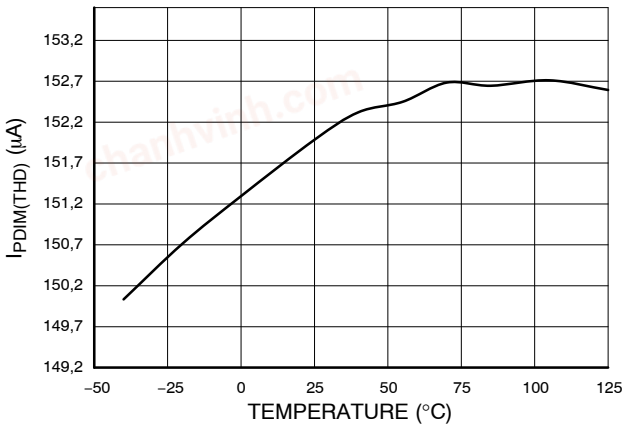


Figure 46. $I_{PDIM(THD)}$ vs. Temperature

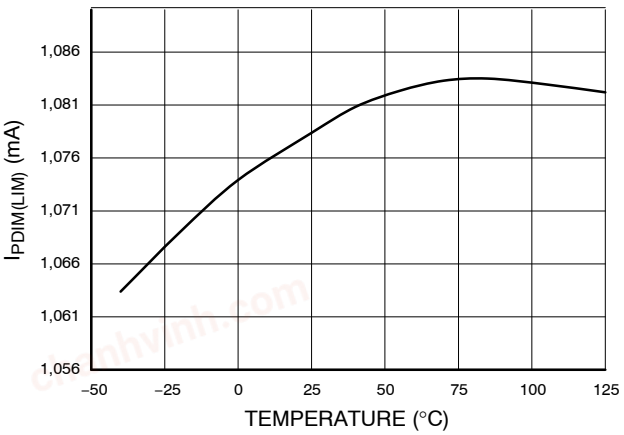


Figure 47. $I_{PDIM(LIM)}$ vs. Temperature

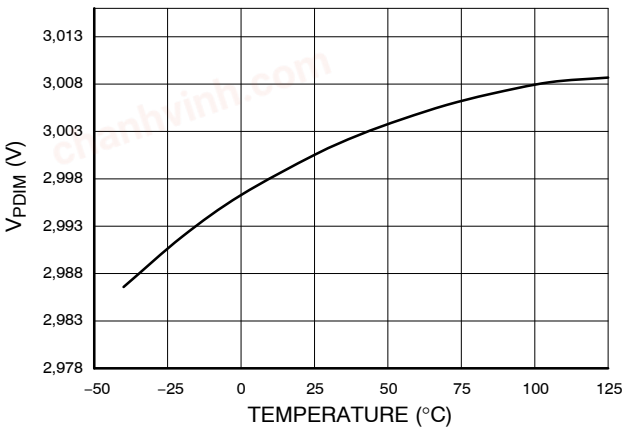


Figure 48. V_{PDIM} vs. Temperature

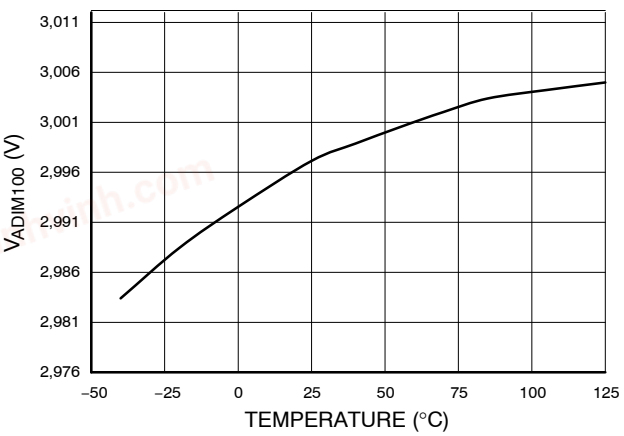


Figure 49. $V_{ADIM100}$ vs. Temperature

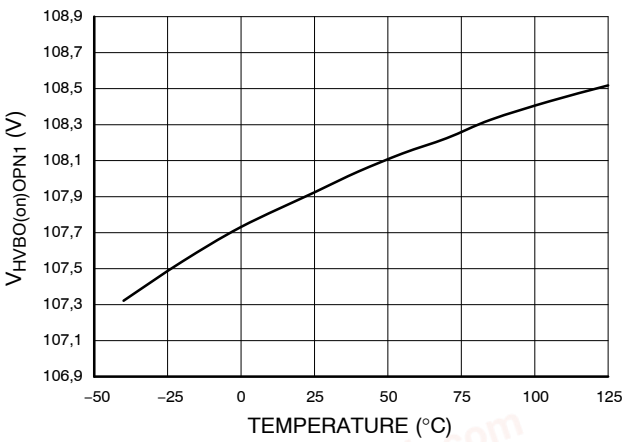


Figure 50. $V_{HVBO(on)ONP1}$ vs. Temperature

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TYPICAL CHARACTERISTICS (continued)

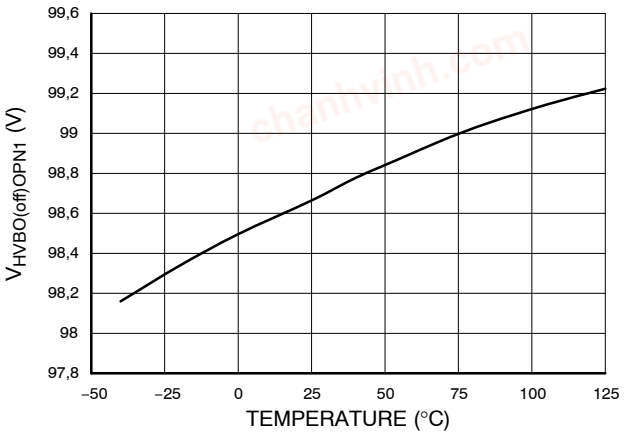


Figure 51. $V_{HVBO(off)ONP1}$ vs. Temperature

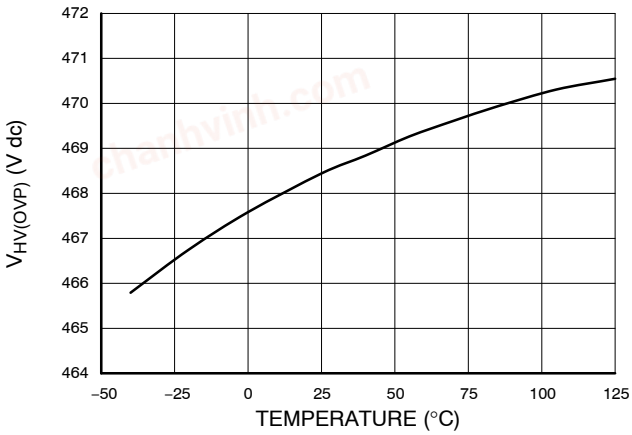


Figure 52. $V_{HV(OVP)}$ vs. Temperature

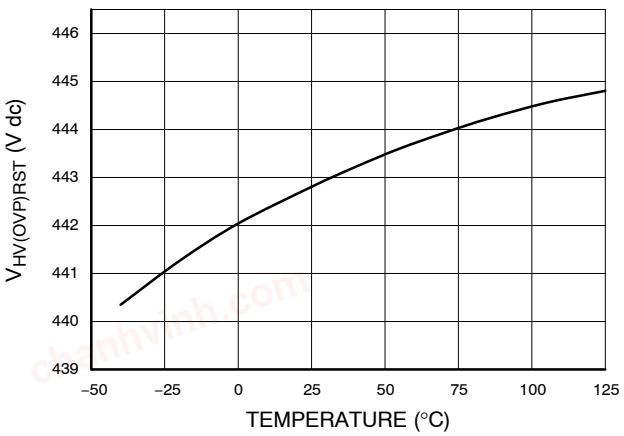


Figure 53. $V_{HV(OVP)RST}$ vs. Temperature

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Application Information

The NCL30486 implements a current−mode architecture operating in quasi−resonant mode. Thanks to proprietary circuitry, the controller is able to accurately regulate the secondary side current and voltage of the fly−back converter without using any opto−coupler or measuring directly the secondary side current or voltage. The controller provides near unity power factor correction

- *Quasi−Resonance Current−Mode Operation:* implementing quasi−resonance operation in peak current−mode control, the NCL30486 optimizes the efficiency by switching in the valley of the MOSFET drain−source voltage. Thanks to an internal algorithm control, the controller locks−out in a selected valley and remains locked until the input voltage or the output current set point significantly changes.
- *Primary Side Constant Current Control:* thanks to a proprietary circuit, the controller is able to take into account the effect of the leakage inductance of the transformer and allows an accurate control of the secondary side current regardless of the input voltage and output load variation.
- *Primary Side Constant Voltage Regulation:* By monitoring the auxiliary winding voltage, it is possible to regulate accurately the output voltage. The output voltage regulation is typically within ±2%.
- *Load Transient Compensation:* Since PFC has low loop bandwidth, abrupt changes in the load may cause excessive over or under−shoot. The slow Over Voltage Protection contains the output voltage when it tends to become excessive. In addition, the NCL30486 speeds up the constant voltage regulation loop when the output voltage goes below 80% or 85% of its regulation level.
- *Power Factor Correction:* A proprietary concept allows achieving high power factor correction and low THD while keeping accurate constant current and constant voltage control.
- *Line Feed−forward:* allows compensating the variation of the output current caused by the propagation delay.
- *V_{CC} Over Voltage Protection:* if the V_{CC} pin voltage exceeds an internal limit, the controller shuts down and waits 4 seconds before restarting pulsing.
- *Fast Over Voltage Protection:* If the voltage of ZCD pin exceeds 130% of its regulation level, the controller shuts down and waits 4 s before trying to restart.
- *Brown−Out:* the controller includes a brown−out circuit which safely stops the controller in case the input voltage is too low. The device will automatically restart if the line recovers.
- *Cycle−by−cycle peak current limit:* when the current sense voltage exceeds the internal threshold V_{ILIM}, the MOSFET is turned off for the rest of the switching cycle.
- *Winding Short−Circuit Protection:* an additional comparator senses the CS signal and stops the controller if V_{CS} reaches 1.5 x V_{ILIM} (after a reduced LEB of t_{BCS}). This additional comparator is enabled only during the main LEB duration t_{LEB}, for noise immunity reason.
- *Output Under Voltage Protection:* If a too low voltage is applied on ZCD pin for 90 ms time interval, the controllers assume that the output or the ZCD pin is shorted to ground and shutdown. After waiting 4 seconds, the IC restarts switching.
- *Analog Dimming:* the ADIM pin is dedicated to analog dimming. There are several options for the minimum dimming level. Pulling the pin voltage lower than $V_{ADIM(EN)}$ disables the controller.
- *PWM dimming:* the PDIM pin is dedicated to PWM dimming. The controller measures the duty ratio of a signal applied to the pin and reduces the output current accordingly. If this pin is left open, the controller delivers the maximum output current. If the pin is pulled down, the controller is disabled.
- *Thermal Shutdown:* an internal circuitry disables the gate drive when the junction temperature exceeds 150°C (typically). The circuit resumes operation once the temperature drops below approximately 100°C.

POWER FACTOR AND CONSTANT CURRENT CONTROL

The NCL30486 embeds an analog/digital block to control the power factor and regulate the output current by monitoring the ZCD, CS and HV pin voltages (signals V_{ZCD}, V_{HV_DIV}, V_{CS}). This circuit generates the current setpoint signal and compares it to the current sense signal to turn the MOSFET off. The HV pin provides the sinusoidal reference necessary for shaping the input current. The obtained current reference is further modulated so that when averaged over a half line period, it is equal to the output current reference (V_{REFX}). The modulation and averaging process is made internally by a digital circuit. If the HV pin properly conveys the sinusoidal shape, power factor will be close to 1. Also, the Total Harmonic Distortion (THD) will be low especially if the output voltage ripple is small.

$$I_{OUT} = \frac{V_{REF}}{2N_{sp}R_{sense}} \quad \text{(eq. 1)}$$

Where:

- N_{sp} is the secondary to primary transformer turns ratio: $N_{sp} = N_S / N_P$
- R_{sense} is the current sense resistor
- V_{REFX} is the output current reference: $V_{REFX} = V_{REF}$ if no dimming

The output current reference (V_{REFX}) is V_{REF} unless the constant voltage mode is activated or ADIM pin voltage is below $V_{ADIM(100)}$ or a PWM signal with a duty−cycle below 95% is applied on PDIM.

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PRIMARY SIDE CONSTANT VOLTAGE CONTROL

The auxiliary winding voltage is sampled internally through the ZCD pin.

A precise internal voltage reference $V_{REF(CV)}$ sets the voltage target for the CV loop.

The sampled voltage is applied to the negative input of the constant voltage (CV) operational transconductance amplifier (OTA) and compared to V_{REFCV}.

A type 2 compensator is needed at the CV OTA output to stabilize the loop. The COMP pin voltage modify the the output current internal reference in order to regulate the output voltage.

When $V_{COMP} \geq 4$ V, $V_{REFX} = V_{REF}$.

When $V_{COMP} < 0.9$ V, $V_{REFX} = 0$ V.

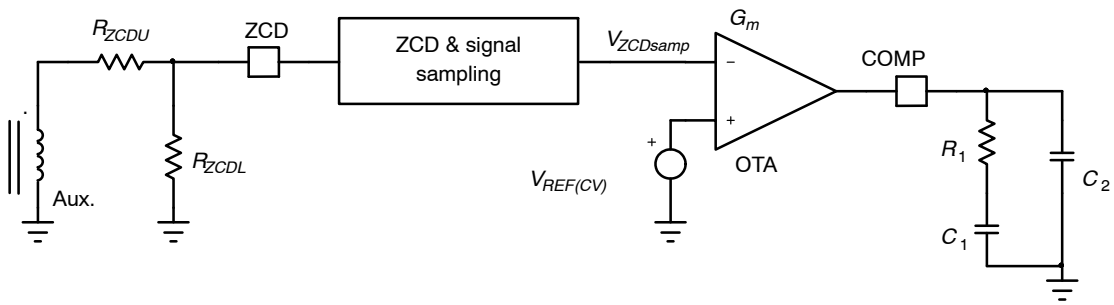


Figure 54. Constant Voltage Feedback Circuit

Secondary Side Regulation Compatible

The NCL30486 is able to support secondary−side regulation as well. The controller features an option to provide a pullup resistor R_{pullup} on COMP pin instead of the CV OTA output. This allows connecting directly an optocoupler collector and properly biases it. The internal voltage biasing R_{pullup} is around 5 V.

In secondary side regulation, the slow and fast OVP on ZCD pin are still active thus providing an additional over voltage protection. In this case, the ZCD pin resistors should be calculated to trigger V_{OVP2} at the output voltage of interest.

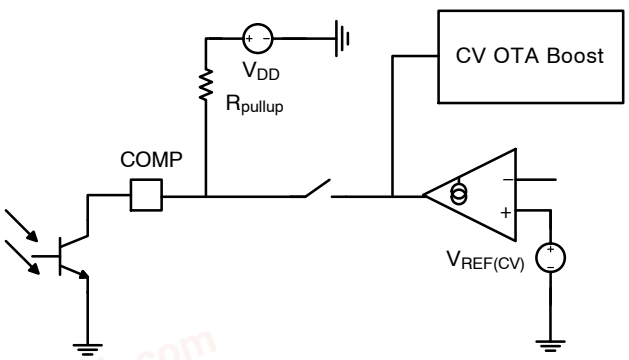


Figure 55. COMP Pin Configuration for Secondary Side Regulation

STARTUP PHASE (HV STARTUP)

It is generally requested that the LED driver starts to emit light in less than 1 s and possibly within 300 ms. It is challenging since the start−up consists of the time to charge the V_{CC} capacitor and that necessary to charge the output capacitor until sufficient current flows into the LED string. This second phase can be particularly long in dimming cases where the secondary current is a portion of the nominal one.

The NCL30486 features a high voltage startup circuit that allows charging VCC capacitor very fast.

When the power supply is first connected to the mains outlet, the internal current source is biased and charges up the V_{CC} capacitor. When the voltage on this V_{CC} capacitor reaches the $V_{CC(on)}$ level, the current source turns off. At this time, the controller is only supplied by the V_{CC} capacitor, and the auxiliary supply should take over before V_{CC} collapses below $V_{CC(off)}$.

The HV startup circuitry is made of two startup current levels, $I_{HV(start1)}$ and $I_{HV(start1)}$. This helps to protect the controller against short−circuit between V_{CC} and GND. At power−up, as long as V_{CC} is below $V_{CC(TH)}$, the source delivers $I_{HV(start1)}$ (around 300 μA typical). Then, when V_{CC} reaches $V_{CC(TH)}$, the source smoothly transitions to $I_{HV(start2)}$ and delivers its nominal value. As a result, in case of short−circuit between V_{CC} and GND occurring at high line (V_{in} = 305 V rms), the maximum power dissipation will be 431 x 300 μ = 130 mW instead of 1.5 W if there was only one startup current level.

To speed−up the output voltage rise, the following is implemented:

- The digital OTA output is increased until $V_{REF(PFC)}$ signal reaches V_{REFX}. Again, this is to speed−up the control signal rise to their steady state value.
- At the beginning of each operating phase of a V_{CC} cycle, the digital OTA output is set to 0. Actually, the digital OTA output is set to 0 in the case of a cold start−up or in the case of a start−up sequence following an operation interruption due to a fault. On the other hand, if the V_{CC} hiccups just because the system fails to start−up in one V_{CC} cycle, the digital OTA output is not reset to ease the second (or more) attempt.

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- If the load is shorted, the circuit will operate in hiccup mode with VCC oscillating between $V_{CC(off)}$ and $V_{CC(on)}$ until the output under voltage protection (UVP) trips. UVP is triggered if the ZCD pin voltage does not exceed $V_{ZCD(short)}$ within a 90 ms operation of time. This indicates that the ZCD pin is shorted to ground or that an excessive load prevents the output voltage from rising.

HV Startup Power Dissipation

At high line (305 V rms and above) the power dissipated by the HV startup in case of fault or when the controller is disabled with PDIM becomes high. Indeed, in case of fault, the NCL30486 is directly supplied by the HV rail. When the controller is disabled with PDIM, the optocoupler collector current is also supplied by the controller, since the NCL30486 allows directly connecting the optocoupler transistor to PDIM pin. Thus, the HV startup circuit also supplies the optocoupler transistor in case of faults. The current flowing through the HV startup will heat the controller. It is highly recommended adding enough copper around the controller to decrease the $R_{\theta JA}$ of the controller.

Adding a minimum pad area of 215 mm^2 of 35 μm copper (1 oz) drops the $R_{\theta JA}$ to around 120°C/W (no air flow, $R_{\theta JA}$ measured at ADIM pin)

The PCB layout shown in Figure 56 is a layout example to achieve low $R_{\theta JA}$.

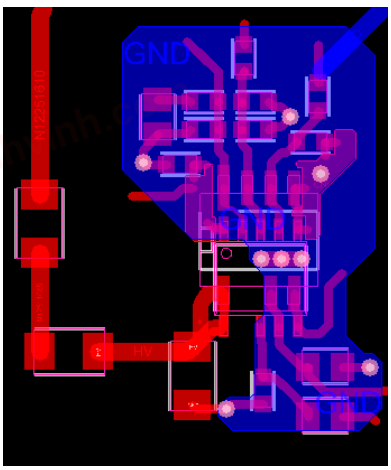


Figure 56. PCD Layout Example

The application note *ANDXXXX* gives more details about strategies to decrease the power dissipation of the HV startup circuit.

Cycle−by−Cycle Current Limit

When the current sense voltage exceeds the internal threshold V_{ILIM}, the MOSFET is turned off for the rest of the switching cycle.

Winding and Output Diode Short−Circuit Protection

In parallel to the cycle−by−cycle sensing of the CS pin, another comparator with a reduced LEB (t_{BCS}) and a threshold of $(V_{CS(stop)} = 140\% \times V_{ILIM})$ monitors the CS pin to detect a winding or an output diode short circuit. The controller shuts down if it detects 4 consecutives pulses during which the CS pin voltage exceeds $V_{CS(stop)}$.

The controller goes into auto−recovery mode.

PWM Dimming

The NCL30486 has a dedicated pin for PWM dimming.

The controller directly measures the duty ratio of a PWM signal applied to PDIM.

Two counters with a high frequency clock are used for this purpose. A first counter measure the high state duration of the PWM signal (t_{on_PDIM}) and the second counter measures its period (T_{sw_PDIM}). A divider computes (t_{on_PDIM} / T_{sw_PDIM}) and the result is directly the output current setpoint (V_{REFX} set point). A filter is added after the digital divider to remove the ripple of the signal. A cascode configuration on PDIM pin allows decreasing the fall time of the signal.

Thanks to this circuit, the LED current is controlled in an analog way, even if a PWM signal is used for dimming. This allows having a good PF during dimming.

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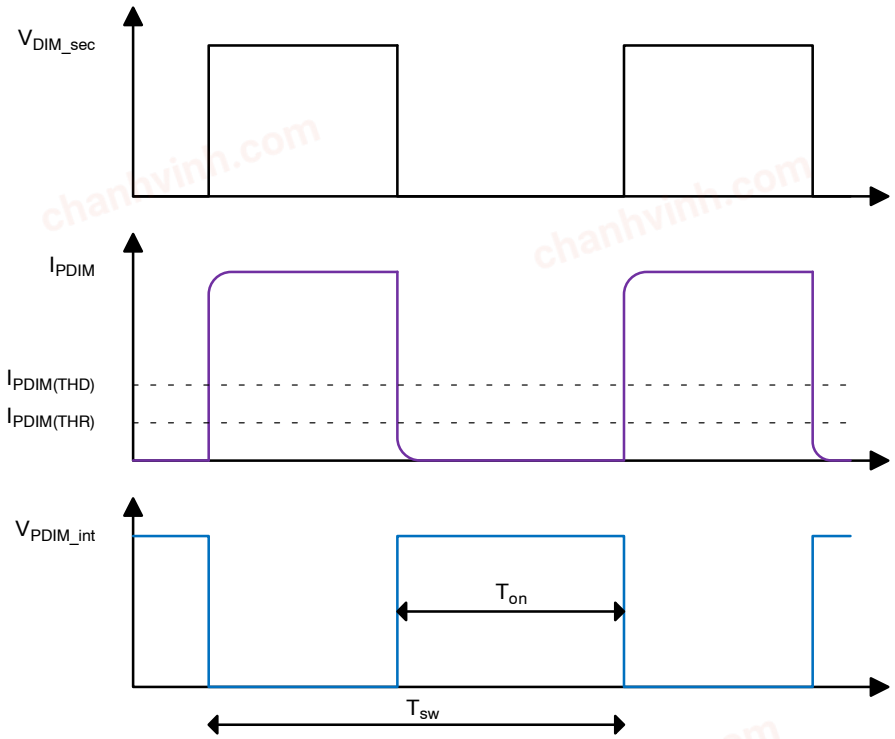


Figure 57. PDIM Internal Waveforms

Practically, the controller extracts the duty−cycle by measuring the current inside PDIM pin which is directly the opto coupler collector current.

If PDIM pin is left open, the controller delivers 100% of I_{out}. If the pin is pulled down for longer than 25 ms, the controller is disabled.

If the PWM dimming signal is removed during dimming, the controller delivers 100% of I_{out}.

The NCL30486 set 100% of output current when the duty−cycle of the signal applied on PDIM is above 93%.

Analog Dimming

The pin ADIM pin allows implementing analog dimming of the LED light.

If the power supply designer applies an analog signal varying from $V_{DIM(EN)}$ to V_{DIM100} to the DIM pin, the output current will increase or decrease proportionally to the voltage applied. For $V_{DIM} = V_{DIM100}$, the power supply delivers the maximum output current (V_{REFX} = 1 V).

If a voltage lower than $V_{ADIM(MIN)}$ is applied to ADIM pin, the output current is clamped to the selected dimming clamp value (see Dimming clamp section below)

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If a voltage lower than $V_{ADIM(EN)}$ is applied to the DIM pin, the DRV pulses are disabled for controllers without the dimming CV mode option.

The DIM pin is pulled up internally by a small current source or resistor. Thus, if the pin is left open, the controller is able to start.

NOTE:

- Interaction between ADIM and PDIM: if ADIM and PDIM are both used at the same time, the resulting dimming set point if a multiplication of V_{ADIM} and the duty−ratio of PDIM signal.
- During dimming, when the “Enable” signal is OK, the controller starts pulsing after 1 time−out pulse, even if a higher valley number is selected by V_{REFX}. This is to avoid too long startup time while dimming at low output current value.

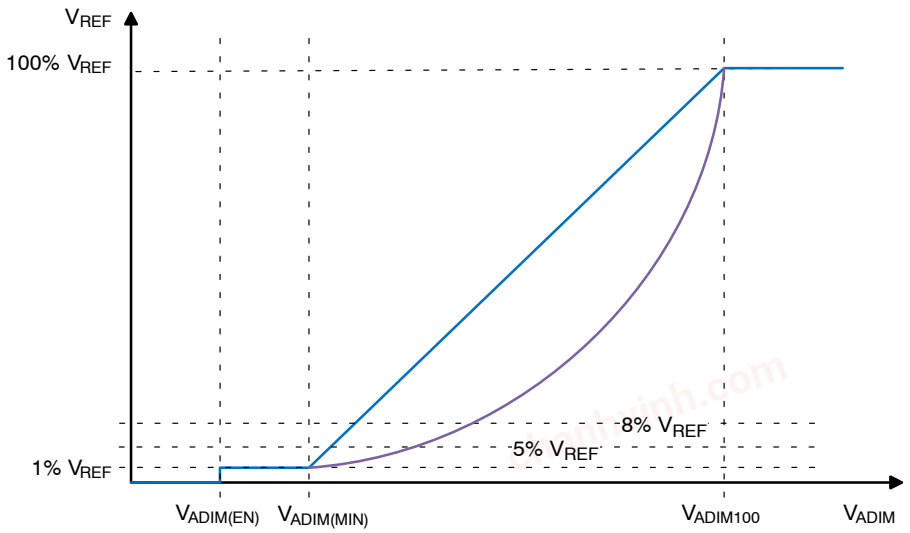


Figure 58. ADIM Pin Dimming Curves

Dimming Clamp

For smart dimming applications, need to bias the secondary−side MCU. This can be achieved by clamping V_{REFX} when the dimming setpoint is small.

There are 4 options for the dimming clamp:

- No dimming clamp
- 1%
- 5%
- 8%

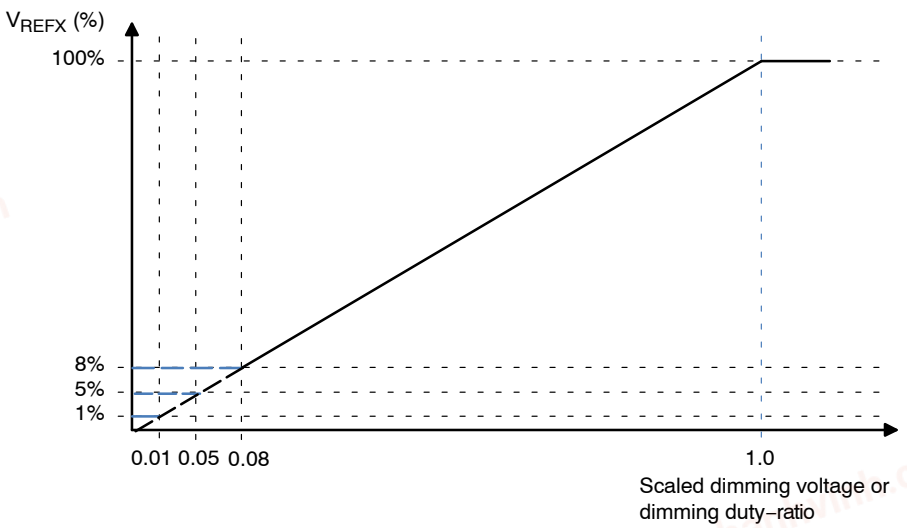


Figure 59. Dimming Clamp Options

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Dimming Curves

By default, there is a linear relationship between the voltage applied on ADIM pin and V_{REFX} setpoint. In the same way, there is a linear relationship between the duty−ratio of the signal applied on PDIM and V_{REFX} setpoint.

An internal memory allows selecting a root square relationship between dimming and V_{REFX}.

The square like curve is based on CIE 1931 lightness formula.

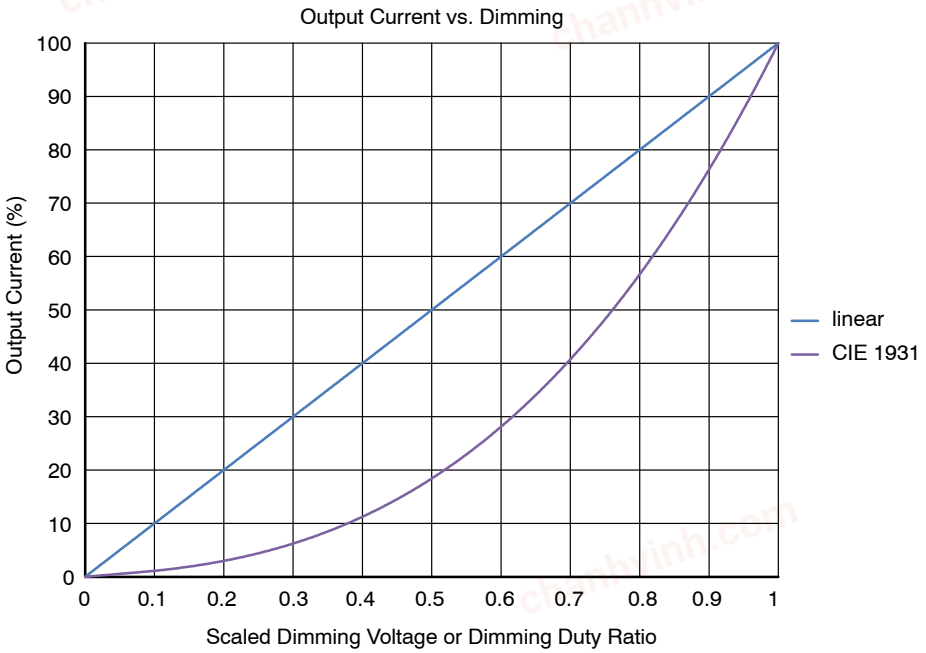


Figure 60. Dimming Curves

Valley Lockout

Quasi−Square wave resonant systems have a wide switching frequency excursion. The switching frequency increases when the output load decreases or when the input voltage increases. The switching frequency of such systems must be limited.

The NCL30486 changes valley as V_{REFX} decreases and as the input voltage increases and as the output current setpoint is varied during dimming. This limits the frequency excursion.

By default, when the output current is not dimmed, the controller operates in the first valley at low line and in the second valley at high line.

There is an option to have the valley thresholds incremented by 1 at high line for better I_{out} control at 305 V rms.

Table 1. VALLEY SELECTION

V_{REFX} value at which the Controller Changes Valley (I_{out} Decreasing)	V_{HV_DIV} Voltage for Valley Change		V_{REFX} Value at Which the Controller Changes Valley(I_{out} Increasing)
	0 −−LL−− 2.3 V	−−HL−− 5 V	
I_{out} decreases ↓	1st	2nd (3rd)	100% ↑ I_{out} decreases
100%			
80%	2nd	3rd (4th)	80%
65%	3rd	4th (5th)	65%
50%	4th	5th (6th)	50%
35%	5th	6th (7th)	35%
25%	FF mode	FF mode	25%
0%			0%
	0 −−LL−− 2.3 V	−−HL−− 5 V	
	Internal V_{HV_DIV} Voltage for Valley Change →		

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Zero Crossing Detection Block

The ZCD pin allows detecting when the drain−source voltage of the power MOSFET reaches a valley.

A valley is detected when the ZCD pin voltage crosses below the 55 mV internal threshold.

At startup or in case of extremely damped free oscillations, the ZCD comparator may not be able to detect the valleys. To avoid such a situation, Optimus Prime features a Time−Out circuit that generates pulses if the voltage on ZCD pin stays below the 55 mV threshold for 6.5 µs.

The Time−out also acts as a substitute clock for the valley detection and simulates a missing valley in case of too damped free oscillations.

At startup, the output voltage reflected on the auxiliary winding is low. Because of the ZCD resistor bridge setting the constant voltage regulation target, the voltage on the ZCD pin is very low and the ZCD comparator might be unable to detect the valleys. In this condition, setting the DRV latch with the 6.5 µs time−out leads to a continuous conduction mode operation (CCM) at the beginning of the soft−start. This CCM operation only last a few cycles until the voltage on ZCD pin becomes high enough and trips the ZCD comparator.

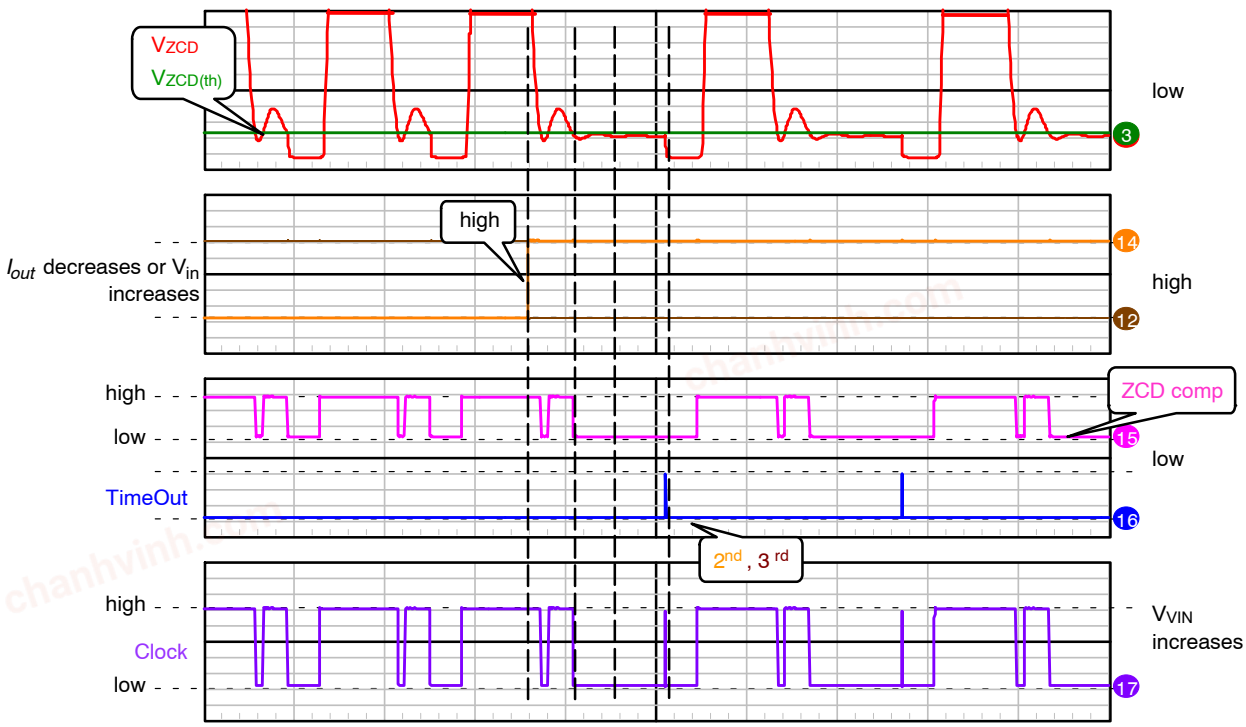


Figure 61. Valley Detection and Time−out Chronograms

If the ZCD pin or the auxiliary winding happen to be shorted the time−out function would normally make the controller keep switching and hence lead to improper regulation of the LED current.

The Under Voltage Protection (UVP) is implemented to avoid these scenarios: a secondary timer starts counting when the ZCD voltage is below the $V_{ZCD(short)}$ threshold. If this timer reaches 90 ms, the controller detects a fault and enters the auto−recovery fault mode.

ZCD Over Voltage Protection

Because of the power factor correction, it is necessary to set the crossover frequency of the CV loop very low (target 10 Hz, depending on power stage phase shift). Because the loop is slow, the output voltage can reach high value during startup or during an output load step. It is necessary to limit the output voltage excursion. For this, the NCL30486 features a slow OVP and a fast OVP on ZCD pin.

Slow OVP

If ZCD voltage exceeds V_{OVP1} for 4 consecutive switching cycles, the controller stops switching during 1.4 ms. The PFC loop is not reset. After 1.4 ms, the controller initiates a new DRV pulse to refresh ZCD sampling voltage. If V_{ZCD} is still too high (V_{ZCD} > 110% $V_{REF(CV)}$), the controller continues to switch with a 1.4 ms period. The controller resumes its normal operation when V_{ZCD} < 110% $V_{REF(CV)}$.

During slow OVP, the peak current setpoint is COMP pin voltage scaled down by a fixed ratio.

Fast OVP

If ZCD voltage exceeds $V_{ZCD(OVP2)}$ (130% of $V_{REF(CV)}$) for 4 consecutive switching cycles (slow OVP not triggered) or for 2 switching cycles if the slow OVP has already been triggered, the controller detects a fault and starts the auto−recovery fault mode (cf: Fault Management Section)

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Line Feedforward

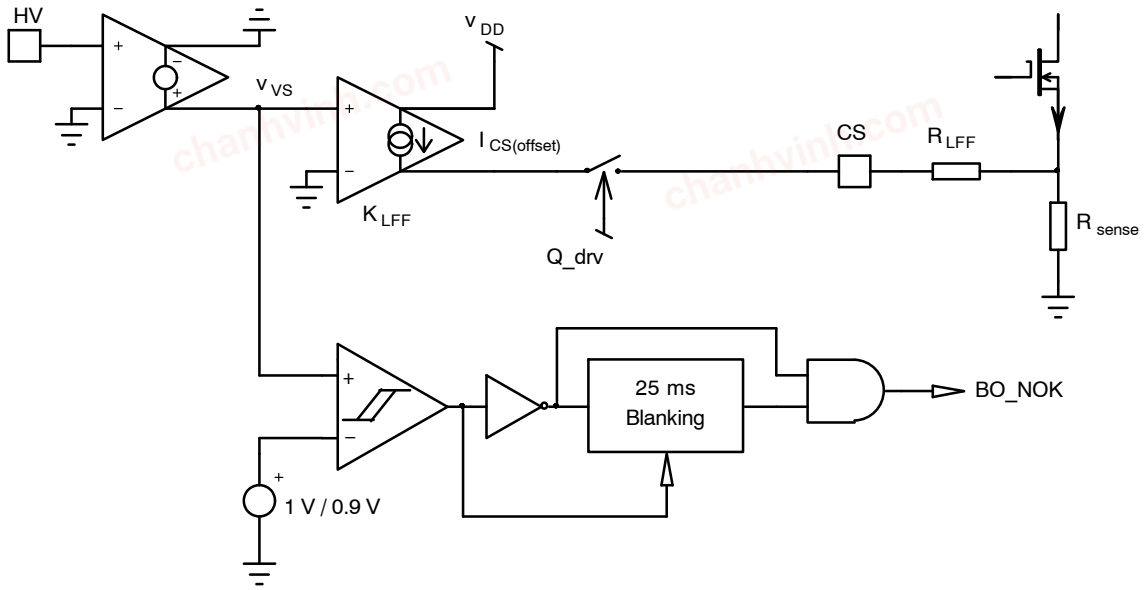


Figure 62. Line Feed−Forward and Brown−out Schematic

The line voltage is sensed by the HV pin and converted into a current. By adding an external resistor in series between the sense resistor and the CS pin, a voltage offset proportional to the line voltage is added to the CS signal. The offset is applied only during the MOSFET on−time in order to not influence the detection of the leakage inductance reset.

The offset is always applied even at light load in order to improve the current regulation at low output load.

Brown−out

In order to protect the supply against a very low input voltage, the controller features a brown−out circuit with a fixed ON/OFF threshold. The controller is allowed to start if a voltage higher than $V_{HVBO(on)}$ is applied to the HV pin and shuts−down if the HV pin voltage decreases and stays below $V_{HVBO(off)}$ for 25 ms typical. Exiting a brown−out condition overrides the hiccup on V_{CC} (V_{CC} does not wait to reach $V_{CC(off)}$) and the IC immediately goes into startup mode.

An option with higher brown−out levels is also available (see ordering table and electricals parameters)

Line OVP

In order to protect the power supply in case of too high input voltage, the NCL30486 features a line over voltage protection. When the voltage on HV pin exceeds $V_{HV(OVP)}$ the controller stops switching; V_{CC} hiccups.

When V_{HV} becomes lower than $V_{HV(OVP)RST}$ for more than 25 ms, the controller initiates a clean startup sequence and re−starts switching.

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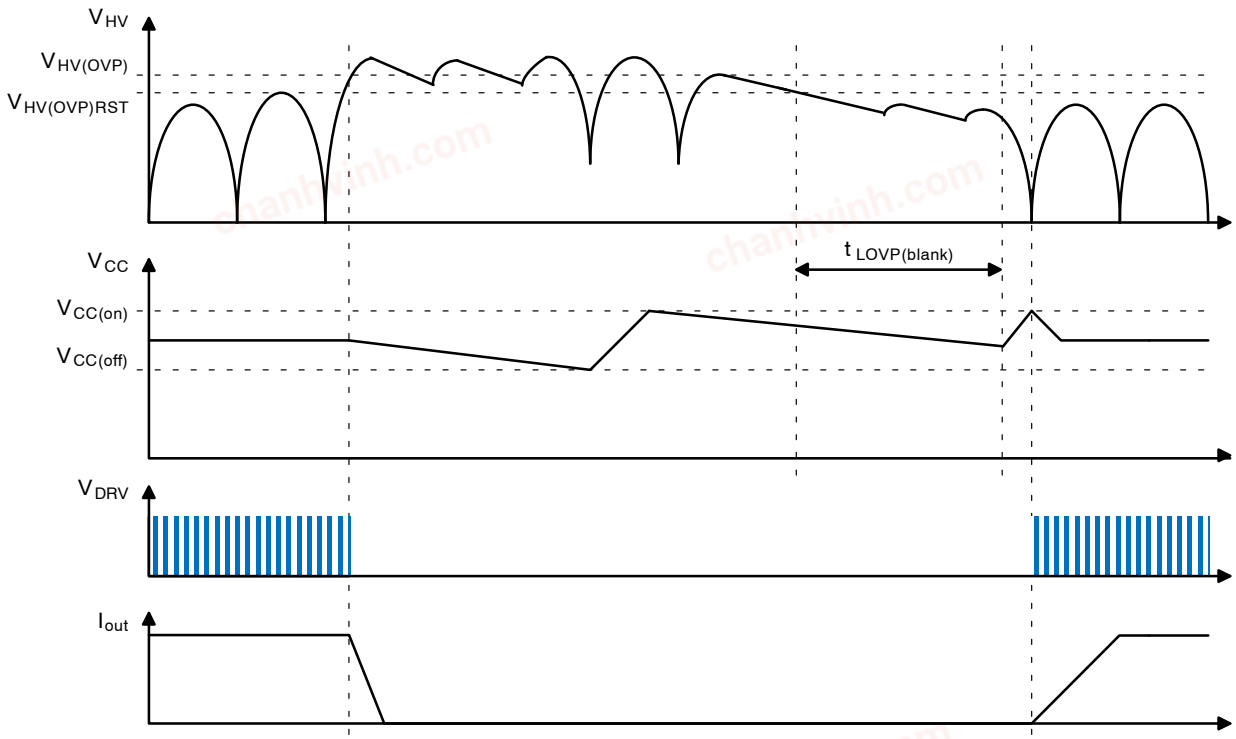


Figure 63. Line OVP Chronograms

Protections

The circuit incorporates a large variety of protections to make the LED driver very rugged.

Among them, we can list:

- Fault of the GND connection
  If the GND pin is properly connected, the supply current drawn from the positive terminal of the V_{CC} capacitor, flows out of the GND pin to return to the negative terminal of the V_{CC} capacitor. If the GND pin is not connected, the circuit ESD diodes offer another return path. The accidental non connection of the GND pin can hence be detected by detecting that one of this ESD diode is conducting. Practically, the ESD diode of CS pin is monitored. If such a fault is detected for 200 µs, the circuit stops generating DRV pin.
- Output short circuit situation (Output Under Voltage Protection)
  Overload is detected by monitoring the ZCD pin voltage: if it remains below $V_{ZCD(short)}$ for 90 ms, an output short circuit is detected and the circuit stops generating pulses for 4 s. When this 4 s delay has elapsed, the circuit attempts to restart.
- ZCD pin incorrect connection:
  - If the ZCD pin grounded, the circuit will detect an output short circuit situation when 90 ms delay has elapsed.
  - A 200 kΩ resistor pulls down the ZCD pin so that the output short circuit detection trips if the ZCD pin is not connected (floating).
- Winding or Output Diode Short Circuit protection
  The circuit detects this failure when 4 consecutive DRV pulses occur within which the CS pin voltage exceeds ($V_{CS(stop)}$ = 140% x V_{ILIM}). In this case, the controller enters auto−recovery mode (4−s operation interruption between active bursts).
- V_{CC} Over Voltage Protection
  The circuit stops generating pulses if the V_{CC} exceeds $V_{CC(OVP)}$ and enters auto−recovery mode. This feature protects the circuit if output LEDs happen to be disconnected.
- ZCD fast OVP
  If ZCD voltage exceeds $V_{ZCD(OVP2)}$ for 4 consecutive switching cycles (slow OVP not triggered) or for 2 switching cycles if the slow OVP has already been triggered, the controller detects a fault and enters auto−recovery mode (4 s operation interruption between active bursts).
- Die Over Temperature (TSD)
  The circuit stops operating if the junction temperature (T_J) exceeds 150°C typically. The controller remains off until T_J goes below nearly 130°C.
- Brown−Out Protection (BO)
  The circuit prevents operation when the line voltage is too low to avoid an excessive stress of the LED driver. Operation resumes as soon as the line voltage is high enough and V_{CC} is higher than $V_{CC(on)}$.

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- CS pin short to ground
  The CS pin is checked at start−up (cold start−up or after a brown−out event). A current source ($I_{cs(short)}$) is applied to the pin and no DRV pulse is generated until the CS pin exceeds $V_{cs(low)}$. $I_{cs(short)}$ and $V_{cs(low)}$ are 500 μA and 60 mV typically (V_{CS} rising). The typical minimum impedance to be placed on the CS pin for operation is then 120 Ω. In practice, it is recommended to place more than 250 Ω to take into account possible parametric deviations. Also, along the circuit operation, the CS pin could happen to be grounded. If it is grounded, the MOSFET conduction time is limited by the 20 μs maximum on−time. If such an event occurs, a new pin impedance test is made.
- Line overvoltage protection
  (see Line OVP section)

ORDERING TABLE OPTION

OPN # NCL30486_ _	Maximum Dead−time			V_{REF}		Max. On−time		ZCD Blanking		Valley Transition from LL to HL		Standby Mode		Line Range Detector	
	250 μs	687 μs	1.4 ms	200 mV	333 mV	20 μs	33 μs	1 μs	1.5 μs	1st to 2nd	1st to 3rd	On	Off	On	Off
NCL30486A2		x			x	x		x		x			x	x	

OPN # NCL30486_ _	Line OVP		Frozen Peak Current During Standby Mode $V_{CS(SBY)}$			Brown−out Levels		Dimming Clamp				Dimming Curve	
	On	Off	380 mV	330 mV	280 mV	On: 108 V Off: 98 V	On: 138 V Off: 129 V	0%	1%	5%	8%	Linear	Square
NCL30486A2	x				NA	x			x			x	

ORDERING INFORMATION

Device	Marking	Package type	Shipping†
NCL30486A2	L30486A2	SOIC9 − P7 COMP VHV PBFH (Pb−Free)	2500 / Tape & Reel

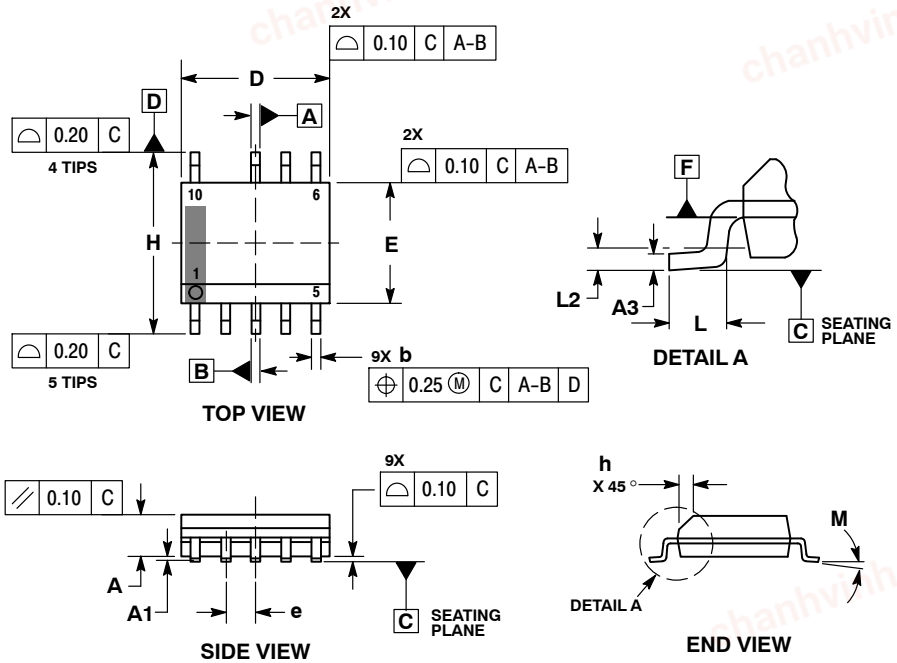
†For information on tape and reel specifications, including part orientation and tape sizes, please refer to our Tape and Reel Packaging Specifications Brochure, BRD8011/D.

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NCL30486

PACKAGE DIMENSIONS

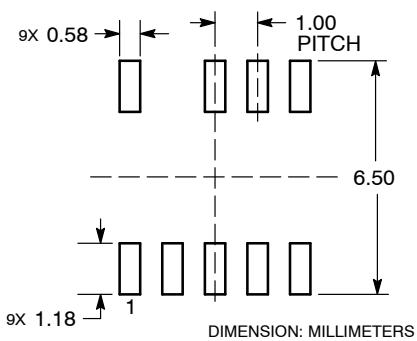
SOIC−9 NB
CASE 751BP
ISSUE A



NOTES:
1. DIMENSIONING AND TOLERANCING PER ASME Y14.5M, 1994.
2. CONTROLLING DIMENSION: MILLIMETERS.
3. DIMENSION b DOES NOT INCLUDE DAMBAR PROTRUSION. ALLOWABLE PROTRUSION SHALL BE 0.10mm TOTAL IN EXCESS OF 'b' AT MAXIMUM MATERIAL CONDITION.
4. DIMENSIONS D AND E DO NOT INCLUDE MOLD FLASH, PROTRUSIONS, OR GATE BURRS. MOLD FLASH, PROTRUSIONS, OR GATE BURRS SHALL NOT EXCEED 0.15mm PER SIDE. DIMENSIONS D AND E ARE DETERMINED AT DATUM F.
5. DIMENSIONS A AND B ARE TO BE DETERMINED AT DATUM F.
6. A1 IS DEFINED AS THE VERTICAL DISTANCE FROM THE SEATING PLANE TO THE LOWEST POINT ON THE PACKAGE BODY.

	MILLIMETERS	
DIM	MIN	MAX
A	1.25	1.75
A1	0.10	0.25
A3	0.17	0.25
b	0.31	0.51
D	4.80	5.00
E	3.80	4.00
e	1.00 BSC	
H	5.80	6.20
h	0.37 REF	
L	0.40	1.27
L2	0.25 BSC	
M	0°	8°

RECOMMENDED SOLDERING FOOTPRINT*



DIMENSION: MILLIMETERS

*For additional information on our Pb−Free strategy and soldering details, please download the ON Semiconductor Soldering and Mounting Techniques Reference Manual, SOLDERRM/D.

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