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BROADCOM®

Data Sheet

ACNT-H79B, ACNT-H79A, ACNT-H790

Optical Isolation Amplifier in 15-mm Stretched SO-8 Package

Description

The Broadcom® ACNT-H79B/H79A/H790 isolation amplifiers are designed for current and voltage sensing in electronic power converters for applications including motor drives and renewable energy systems. In a typical motor drive implementation, current flows through an external resistor and the resulting analog voltage drop is sensed by the isolation amplifier. A differential output voltage that is proportional to the current is created on the other side of the optical isolation barrier.

For general applications, the ACNT-H79A (±1% gain tolerance) and the ACNT-H790 (±3% gain tolerance) are recommended. For high-precision applications, the ACNT-H79B (±0.5% gain tolerance) can be used. The ACNT-H79B/H79A/H790 offers wide creepage and clearance with a high common-mode transient immunity of 15 kV/µs. These features allow the ACNT-H79B/H79A/H790 to provide the precision and stability needed to accurately monitor motor current in high noise motor control environments, providing for smoother control (less “torque ripple”) in various types of motor control applications. The ACNT-H79B/H79A/H790 operates from a single 5V supply and provides excellent linearity and dynamic performance of 60dB SNR. With 200 kHz bandwidth, 1.6-µs fast response time, the ACNT-H79B/H79A/H790 captures transients in short circuit and overload conditions.

Combined with superior optical coupling technology, the ACNT-H79B/H79A/H790 uses sigma-delta (Σ-Δ) analog-to-digital modulation, chopper stabilized amplifiers, and a fully differential circuit topology to provide unequaled isolation-mode noise rejection, low offset, high gain accuracy and stability. This performance is delivered in a compact, auto-insertable 15 mm Stretched SO-8 package that meets worldwide regulatory safety standards.

Features

- ±0.5% gain accuracy (ACNT-H79B)
- –50 ppm/°C low gain drift
- 0.6-mV input offset voltage
- 0.05% excellent linearity
- 60-dB SNR
- 200-kHz wide bandwidth (Typ)
- –40°C to +105°C operating temperature range
- Advanced sigma-delta (Σ-Δ) A/D modulation technology
- 15-mm stretched SO-8 package
- 0.5-mm distance through insulation (DTI)
- 15-kV/µs common-mode transient immunity
- Safety and regulatory approvals:
  - IEC/EN/DIN EN 60747-5-5: 2262Vpeak working insulation voltage
  - UL 1577: 7500Vrms/1min double protection rating
  - CSA: Component Acceptance Notice #5

Applications

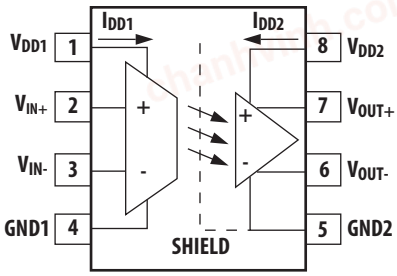
- Current/voltage sensing in AC/servo motor drives
- Mid-voltage drives
- Solar inverters, wind turbine inverters
- Industrial process control
- General-purpose analog signal isolation
- Hall effect current transducer replacements

CAUTION! It is advised that normal static precautions be taken in handling and assembly of this component to prevent damage and/or degradation that may be induced by ESD. The components featured in this data sheet are not to be used in military or aerospace applications or environments.

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Functional Diagram

Figure 1: Functional Diagram



NOTE: A 0.1 µF bypass capacitor mus be connected between pins 1 and 4 and between pins 5 and 8.

Table 1. Pin Description

Pin Number	Symbol	Description
1	VDD1	Supply voltage for input side (4.5V to 5.5V), relative to GND1
2	VIN+	Positive input (±200 mV recommended)
3	VIN–	Negative input (normally connected to GND1)
4	GND1	Input side ground
5	GND2	Output side ground
6	VOUT–	Negative output
7	VOUT+	Positive output
8	VDD2	Supply voltage for output side (3V to 5.5V), relative to GND2

Table 2. Ordering Information

ACNT-H79B/H79A/H790 is UL recognized with 7500 Vrms/1 minute rating per UL 1577.

Part Number	Option (RoHS Compliant)	Package	Surface Mount	Tape and Reel	IEC/EN/DIN EN 60747-5-5	Quantity
ACNT-H790	-000E	15-mm Stretched SO-8	X		X	80 per tube
ACNT-H79A ACNT-H79B	-500E		X	X	X	1000 per reel

To order, choose a part number from the part number column and combine with the desired option from the option column to form an order entry.

Example:

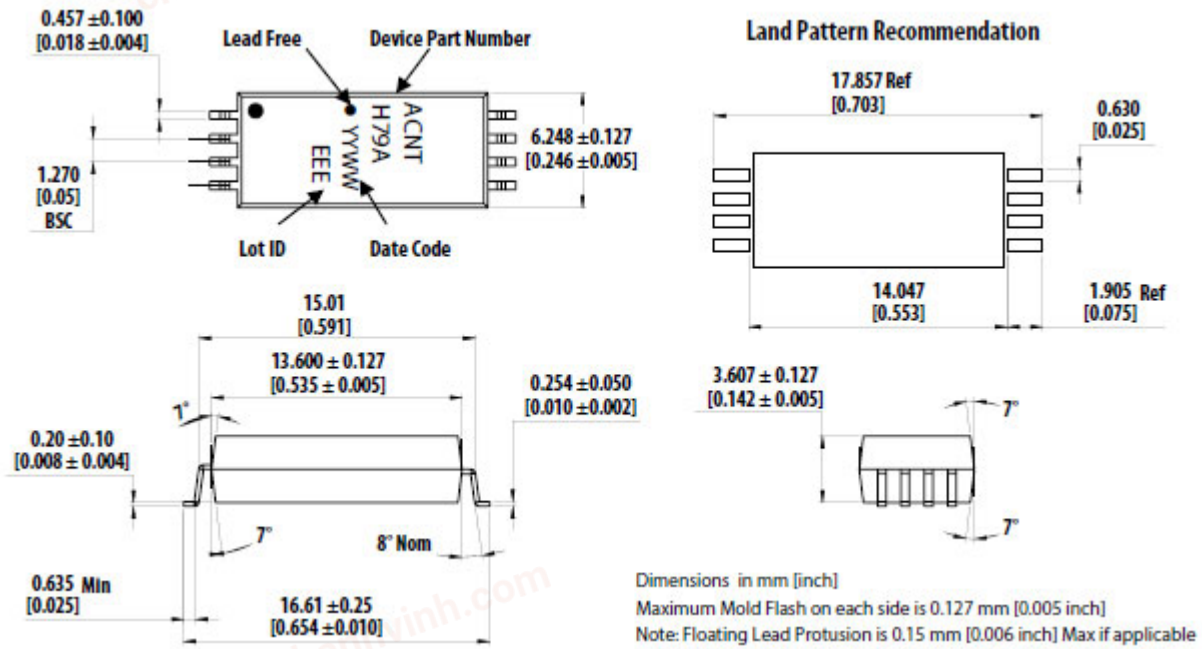
ACNT-H79A-500E to order product of Surface Mount package in Tape and Reel packaging with IEC/EN/DIN EN 60747-5-5 Safety Approval and RoHS compliance.

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Package Outline Drawings

ACNT-H79B, ACNT-H79A, ACNT-H790 Stretched SO-8 Package

Figure 2: ACNT-H79B, ACNT-H79A, ACNT-H790 Stretched SO-8 Package



Recommended Pb-Free IR Profile

Recommended reflow condition as per JEDEC Standard, J-STD-020 (latest revision). Non-Halide Flux should be used.

Regulatory Information

The ACNT-H79B/H79A/H790 is approved by the following organizations.

IEC/EN/DIN EN 60747-5-5	Approved with Maximum Working Insulation Voltage V_{IORM} = 2262V_{peak}.
UL	Approval under UL 1577, component recognition program up to V_{ISO} = 7500 Vrms/1min. File E55361.
CSA	Approval under CSA Component Acceptance Notice #5, File CA 88324.

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Table 3. Insulation and Safety Related Specifications

Parameter	Symbol	Value	Units	Conditions
Minimum External Air Gap (External Clearance)	L(101)	14.2	mm	Measured from input terminals to output terminals, shortest distance through air
Minimum External Tracking (External Creepage)	L(102)	15	mm	Measured from input terminals to output terminals, shortest distance path along body
Minimum Internal Plastic Gap (Internal Clearance)		0.5	mm	Through insulation distance, conductor to conductor, usually the direct distance between the photoemitter and photodetector inside the optocoupler cavity
Tracking Resistance (Comparative Tracking Index)	CTI	>300	V	DIN IEC 112/VDE 0303 Part 1
Isolation Group		IIIa		Material Group (DIN VDE 0110, 1/89, Table 1)

Table 4. IEC/EN/DIN EN 60747-5-5 Insulation Characteristics (See Note)

Description	Symbol	Value	Units
Installation classification per DIN VDE 0110/1.89, Table 1			
for rated mains voltage ≤ 150 V_{rms}		I-IV	
for rated mains voltage ≤ 300 V_{rms}		I-IV	
for rated mains voltage ≤ 450 V_{rms}		I-IV	
for rated mains voltage ≤ 600 V_{rms}		I-IV	
for rated mains voltage ≤ 1000 V_{rms}		I-IV	
Climatic Classification		55/105/21	
Pollution Degree (DIN VDE 0110/1.89)		2	
Maximum Working Insulation Voltage	V_{IORM}	2262	V_{peak}
Input to Output Test Voltage, Method b V_{IORM} × 1.875 = V_{PR}, 100% Production Test with t_m = 1 second, Partial Discharge < 5 pC	V_{PR}	4242	V_{peak}
Input to Output Test Voltage, Method a V_{IORM} × 1.6 = V_{PR}, Type and Sample Test, t_m = 10 seconds, Partial Discharge < 5 pC	V_{PR}	3619	V_{peak}
Highest Allowable Overvoltage (Transient Overvoltage, t_{ini} = 60 sec)	V_{IOTM}	12000	V_{peak}
Safety-limiting values (Maximum values allowed in the event of a failure)			
Case Temperature	T_S	175	°C
Input Current	$I_{S,INPUT}$	230	mA
Output Power	$P_{S,OUTPUT}$	600	mW
Insulation Resistance at T_S, V_{IO} = 500 V	R_S	$>10^9$	Ω

NOTE: Insulation characteristics are guaranteed only within the safety maximum ratings, which must be ensured by protective circuits within the application.

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Table 5. Absolute Maximum Rating

Parameter	Symbol	Min.	Max.	Units
Storage Temperature	T_S	–55	+125	°C
Ambient Operating Temperature	T_A	–40	+105	°C
Supply Voltages	V_{DD1}, V_{DD2}	–0.5	6.0	V
Steady-State Input Voltage[a, b]	V_{IN+}, $V_{IN–}$	–2	V_{DD1} + 0.5	V
Two-Second Transient Input Voltage[c]	V_{IN+}, $V_{IN–}$	–6	V_{DD1} + 0.5	V
Output Voltages	V_{OUT+}, $V_{OUT–}$	–0.5	V_{DD2} + 0.5	V
Lead Solder Temperature	260°C for 10 sec., 1.6 mm below seating plane			

a. DC voltage of up to –2 V on the inputs does not cause latch-up or damage to the device; tested at typical operating conditions.

b. Absolute maximum DC current on the inputs = 100 mA, no latch-up or device damage occurs.

c. Transient voltage of 2 seconds up to –6V on the inputs does not cause latch-up or damage to the device; tested at typical operating conditions.

Table 6. Recommended Operating Conditions

Parameter	Symbol	Min.	Max.	Units
Ambient Operating Temperature	T_A	–40	+105	°C
V_{DD1} Supply Voltage	V_{DD1}	4.5	5.5	V
V_{DD2} Supply Voltage	V_{DD2}	3	5.5	V
Input Voltage Range[a]	V_{IN+}, $V_{IN–}$	–200	+200	mV

a. ±200 mV is the nominal input range. Full scale input range (FSR) is ±300 mV. Functional input range is ±2V.

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Table 7. Electrical Specifications

Unless otherwise noted, T_A = –40°C to +105°C, V_{DD1} = 4.5V to 5.5V, V_{DD2} = 3V to 5.5V, V_{IN+} = –200 mV to +200 mV, and $V_{IN–}$ = 0 V (single-ended connection).

Parameter	Symbol	Min.	Typ. [a]	Max.	Unit	Test Conditions/Notes	Figure
DC Characteristics							
Input Offset Voltage	V_{OS}	–2	-0.2	2	mV	T_A = 25°C	3, 4
Magnitude of Input Offset Change vs. Temperature	$\lvert dV_{OS}/dT_A \rvert$	—	0.6	5	µV/°C	T_A = –40°C to +105°C; absolute value	5
Gain (ACNT-H79B, ±0.5%)	G0	8.16	8.2	8.24	V/V	T_A = 25°C; Note [b], V_{DD1}= 5V	6, 7
Gain (ACNT-H79A, ±1%)	G1	8.14	8.2	8.26	V/V	T_A = 25°C; Note [b], V_{DD1}= 5V	6, 7
Gain (ACNT-H790, ±3%)	G3	7.97	8.2	8.42	V/V	TA = 25°C; Note [b], V_{DD1}= 5V	6, 7
Gain Change vs. V_{DD1}	dG/dV_{DD1}	—	0.0041	—	V/V/V		
Magnitude of Gain Change vs. Temperature	dG/dT_A	—	–0.00041	—	V/V/°C	T_A = –40°C to +105°C; Note [c]	
Nonlinearity over ±200 mV Input Voltage	NL_{200}	—	0.055	0.13	%	V_{IN+} = –200 mV to +200 mV, T_A = 25°C; Note [b]	9, 10
Magnitude of NL200 Change vs. Temperature	dNL_{200}/dT_A	—	0.0003	—	%/°C	TA = –40°C to +105°C	11
Nonlinearity over ±100 mV Input Voltage	NL_{100}	—	0.015	0.06	%	V_{IN+} = –100 mV to +100 mV, T_A = 25°C; Note [b]	9, 10, 11
Inputs and Outputs							
Full-Scale Differential Voltage Input Range	FSR	—	±300	—	mV	$V_{IN} = V_{IN}+ – V_{IN–}$; Note [d]	12
Input Bias Current	I_{IN+}	–1	–0.1	—	µA	V_{IN+} = 0, $V_{IN–}$ = 0 V; Note [e]	13
Magnitude of IIN+ Change vs. Temperature	dI_{IN+}/dT_A	—	–0.05	—	nA/°C		
Equivalent Input Impedance	R_{IN}	—	27	—	kΩ	V_{IN+} or $V_{IN–}$, single-ended	14
Output Common-Mode Voltage	V_{OCM}	—	1.23	—	V	V_{OUT+} or V_{OUT-}; Note [f]	
Output Voltage Range	OVR	—	0 to 2.65	—	V	V_{OUT+} or V_{OUT-}; Note [d]	12
Output Short-Circuit Current	$\lvert I_{OSC} \rvert$	—	11	—	mA	V_{OUT+} or V_{OUT-}, shorted to GND2 or V_{DD2}	
Output Resistance	R_{OUT}	—	21	—	Ω	V_{OUT+} or V_{OUT-}	
Input DC Common-Mode Rejection Ratio	$CMRR_{IN}$	—	76	—	dB	Note [b]	
AC Characteristics							
Signal-to-Noise Ratio	SNR	—	60	—	dB	VIN+ = 300 mVpp 10 kHz sine wave; Note [g]	15, 16
Signal-to-(Noise + Distortion) Ratio	SNDR	—	56	—	dB	VIN+ = 300 mVpp 10 kHz sine wave; Note [h]	15, 16
Small-Signal Bandwidth (–3 dB)	$f_{–3\ dB}$	140	200	—	kHz		17, 18

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Parameter		Symbol	Min.	Typ. [a]	Max.	Unit	Test Conditions/Notes	Figure
Input to Output Propagation Delay	10%-10%	t_{PD10}	—	1.6	2.3	µs	200 mV/µs step input	19
	50%-50%	t_{PD50}	—	2.0	2.6	µs	200 mV/µs step input	19
	90%-90%	t_{PD90}	—	2.6	3.3	µs	200 mV/µs step input	19
Output Rise/Fall Time (10%-90%)		$t_{R/F}$	—	1.7	—	µs	Step input	19
Common Mode Transient Immunity		CMTI	15	20	—	kV/µs	V_{CM} = 1 kV, T_A = 25°C; Note [b]	
Power Supply Rejection		PSR	—	–78	—	dB	1 Vpp 1 kHz sine wave ripple on V_{DD1}, differential output; Note [i]	
Power Supplies								
Input Side Supply Current		I_{DD1}	—	19	28	mA	V_{IN+} =±400 mV; see Note [j]	20
Output Side Supply Current		I_{DD2}	—	7	11	mA	5 V supply	20
			—	6.5	10	mA	3.3 V supply	20

a. All Typical values are under Typical Operating Conditions at T_A = 25°C, V_{DD1} = 5V, V_{DD2} = 3.3V.

b. See Definitions.

c. Gain temperature drift can be normalized and expressed as Temperature Coefficient of Gain (TCG) of –50 ppm/°C.

d. When FSR is exceeded, outputs saturate.

e. Because of the switched-capacitor nature of the input sigma-delta converter, time-averaged values are shown.

f. Under Typical Operating Conditions, part-to-part variation ±0.04V.

g. Under Typical Operating Conditions, part-to-part variation ±1 dB.

h. Under Typical Operating Conditions, part-to-part variation ±1 dB.

i. Ripple voltage applied to V_{DD1} with a 0.1 µF bypass capacitor connected; differential amplitude of the ripple outputs measured. See Definitions.

j. The input supply current decreases as the differential input voltage (V_{IN+} – $V_{IN–}$) decreases.

Table 8. Package Characteristics

Parameter	Symbol	Min.	Typ.	Max.	Unit	Test Condition	Note
Input-Output Momentary Withstand Voltage	V_{ISO}	7500	—	—	Vrms	RH < 50%, t = 1 min., T_A = 25°C	a, b
Resistance (Input-Output)	R_{I-O}	—	10^9	—	Ω	V_{I-O} = 500 VDC	c
Capacitance (Input-Output)	C_{I-O}	—	0.5	—	pF	f = 1 MHz	c

a. In accordance with UL 1577, each optocoupler is proof tested by applying an insulation test voltage ≥ 9000Vrms for 1 second (leakage detection current limit, I_{I-O} ≤ 5µ A). This test is performed before the 100% production test for partial discharge (method b) shown in IEC/EN/DIN EN 60747-5-5 Insulation Characteristic Table.

b. The Input-Output Momentary Withstand Voltage is a dielectric voltage rating that should not be interpreted as an input-output continuous voltage rating. For the continuous voltage rating, refer to the IEC/EN/DIN EN 60747-5-5 insulation characteristics table and your equipment level safety specification.

c. This is a two-terminal measurement: pins 1–4 are shorted together and pins 5–8 are shorted together.

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Typical Performance Plots

Unless otherwise noted, T_A = 25°C, V_{DD1} = 5V, V_{DD2} = 3.3V.

Figure 3: Input Offset vs. Supply V_{DD1}

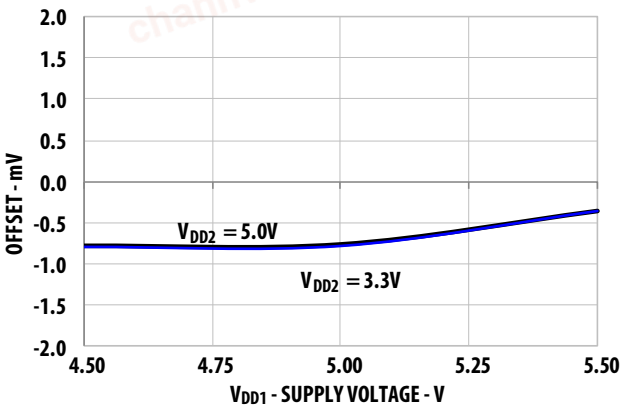


Figure 4: Input Offset vs. Supply V_{DD2}

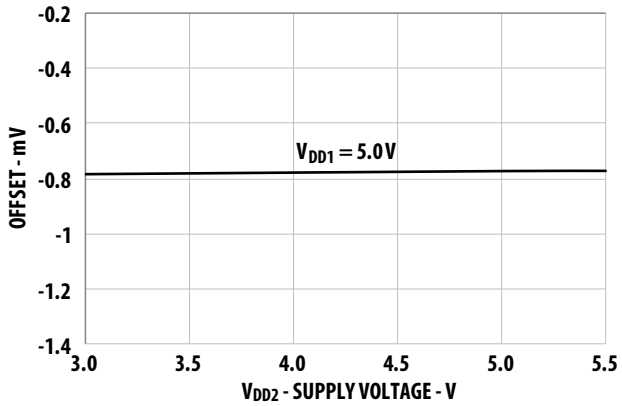


Figure 5: Input Offset vs. Temperature

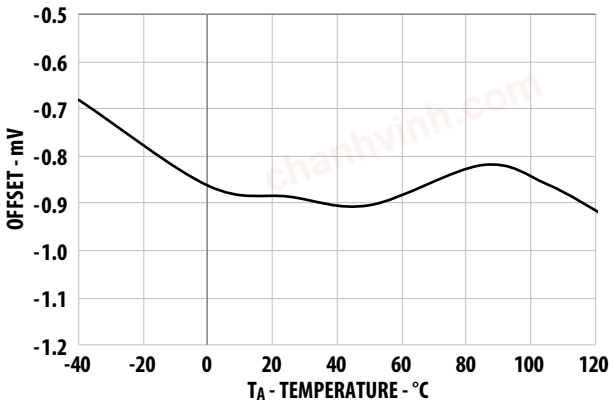


Figure 6: Gain vs. Supply V_{DD1}

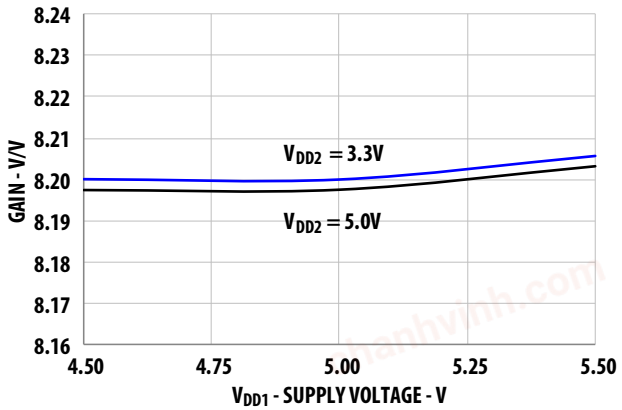


Figure 7: Gain vs. Supply V_{DD2}

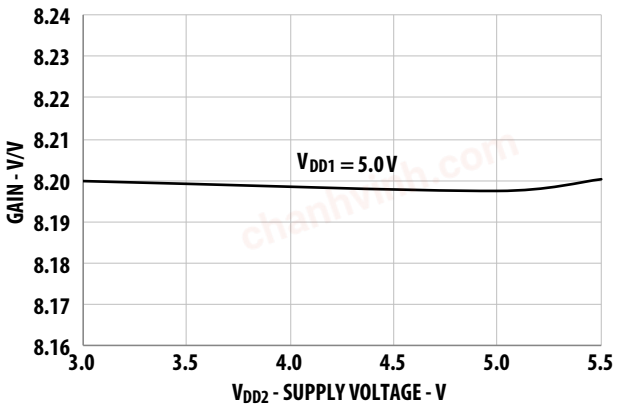
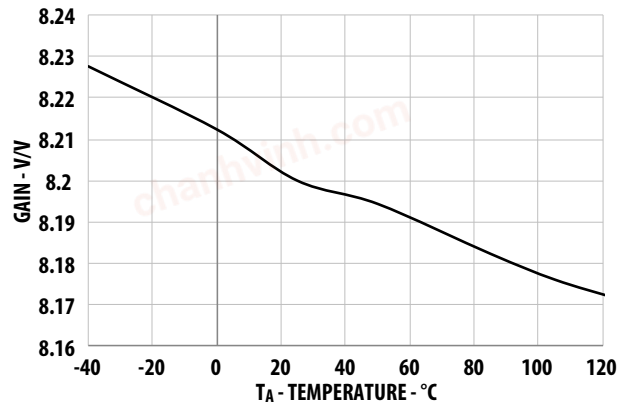


Figure 8: Gain vs. Temperature



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Figure 9: Nonlinearity vs. Supply V_{DD1}

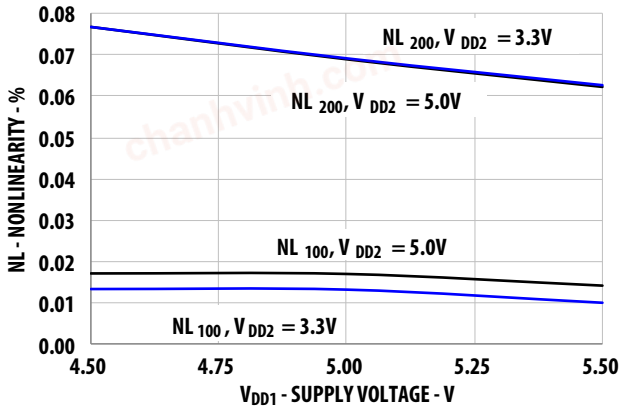


Figure 10: Nonlinearity vs. Supply V_{DD1}

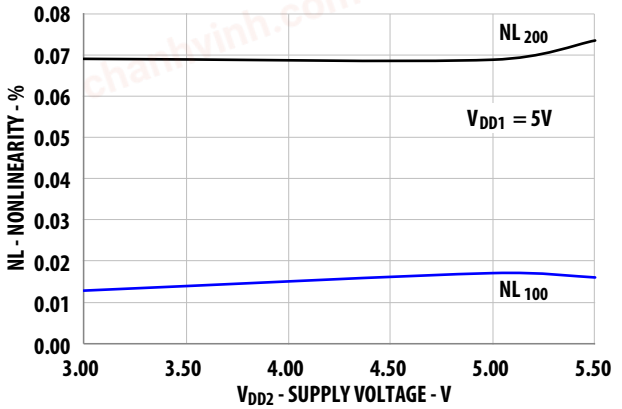


Figure 11: Nonlinearity vs. Temperature

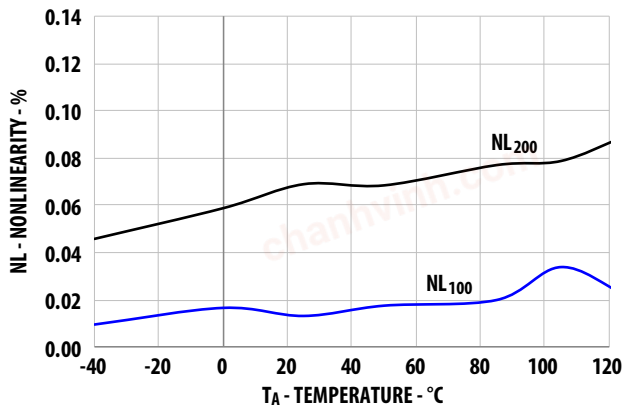


Figure 12: Output Voltage vs. Input Voltage

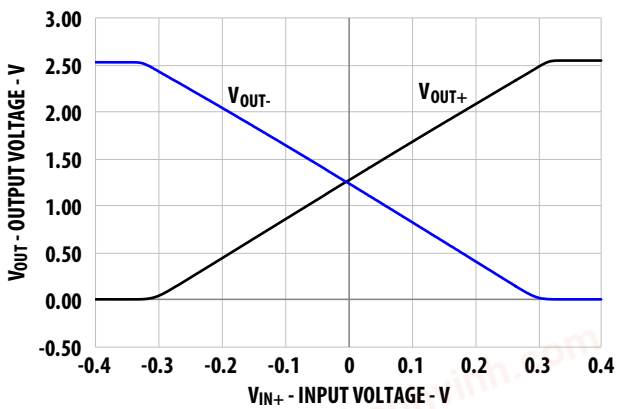


Figure 13: Input Current vs. Input Voltage

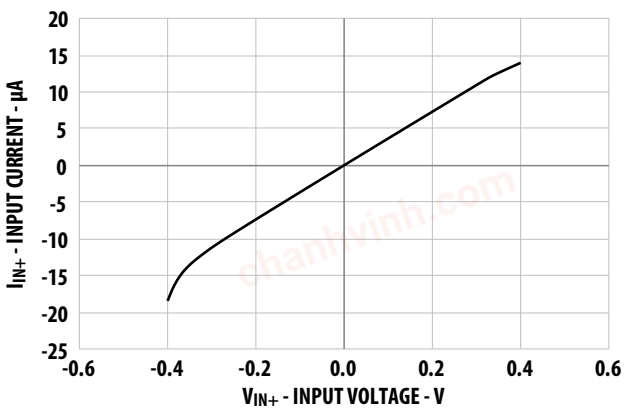
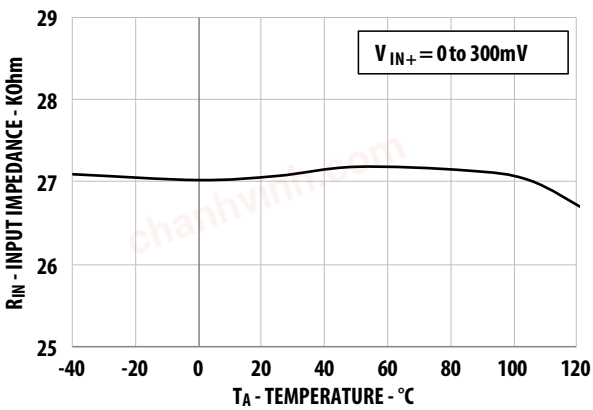


Figure 14: Input Impedance vs. Temperature



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Figure 15: SNR, SNDR vs. Temperature

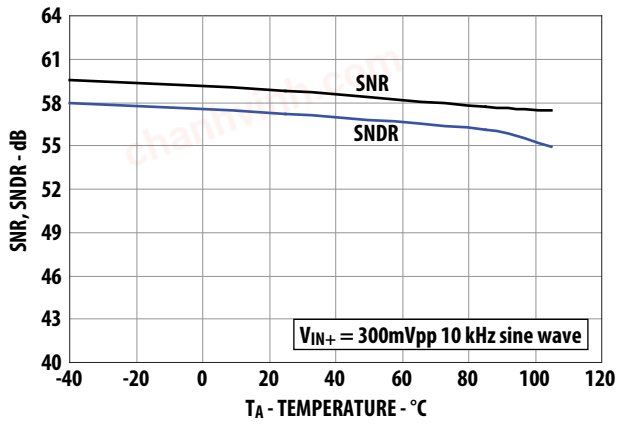


Figure 16: SNR, SNDR vs. Input Voltage

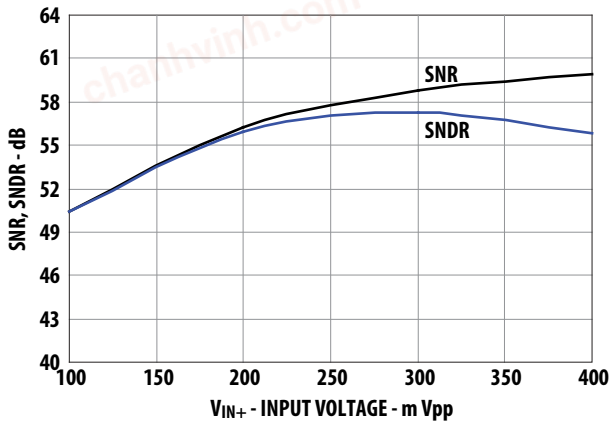


Figure 17: Gain Frequency Response

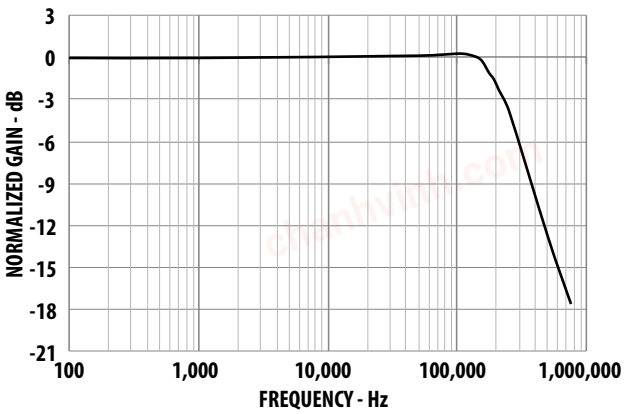


Figure 18: Phase Frequency Response

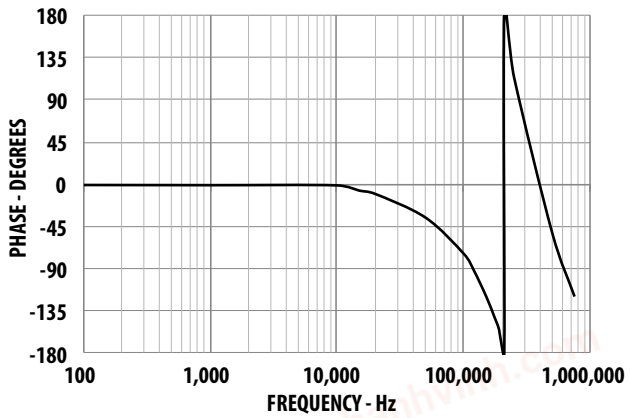


Figure 19: Propagation Delay, Output Rise/Fall vs. Temperature

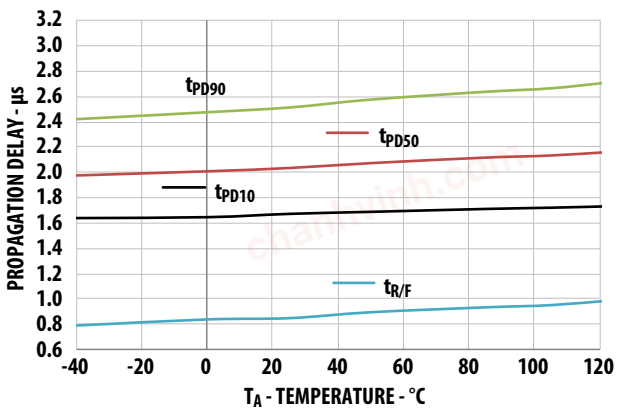
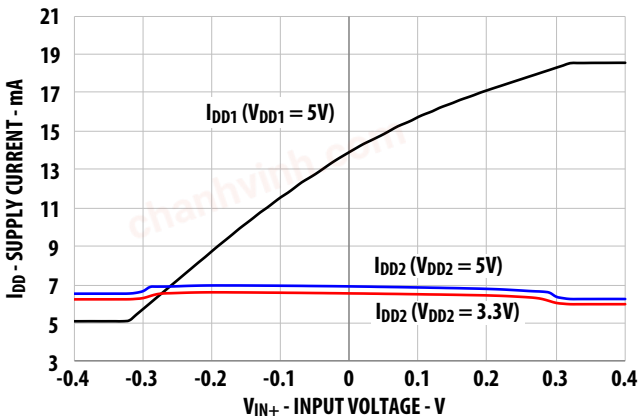


Figure 20: Supply Current vs. Input Voltage



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Definitions

Gain

Gain is defined as the slope of the best-fit line of differential output voltage ($V_{OUT+} – V_{OUT–}$) vs. differential input voltage ($V_{IN+} – V_{IN–}$) over the nominal input range, with offset error adjusted out.

Nonlinearity

Nonlinearity is defined as half of the peak-to-peak output deviation from the best-fit gain line, expressed as a percentage of the full-scale differential output voltage.

Input DC Common Mode Rejection Ratio, $CMRR_{IN}$

$CMRR_{IN}$ is defined as the ratio of the differential signal gain (signal applied differentially between pins V_{OUT+} and $V_{OUT–}$) to the input side common-mode gain (input pins tied together and the signal applied to both inputs with respect to pin GND1), expressed in dB.

Common Mode Transient Immunity, CMTI, also known as Common Mode Rejection

CMTI is tested by applying an exponentially rising/falling voltage step on pin 4 (GND1) with respect to pin 5 (GND2). The amplitude of the step is adjusted until the differential output ($V_{OUT+} – V_{OUT-}$) exhibits more than a 200 mV deviation from the average output voltage for more than 1µs. The ACNT-H79B/H79A/H790 will continue to function if more than 15 kV/µs common mode slopes are applied, as long as the breakdown voltage limitations are observed.

Power Supply Rejection, PSR

PSR is the ratio of differential amplitude of the ripple outputs over power supply ripple voltage, referred to the input, expressed in dB.

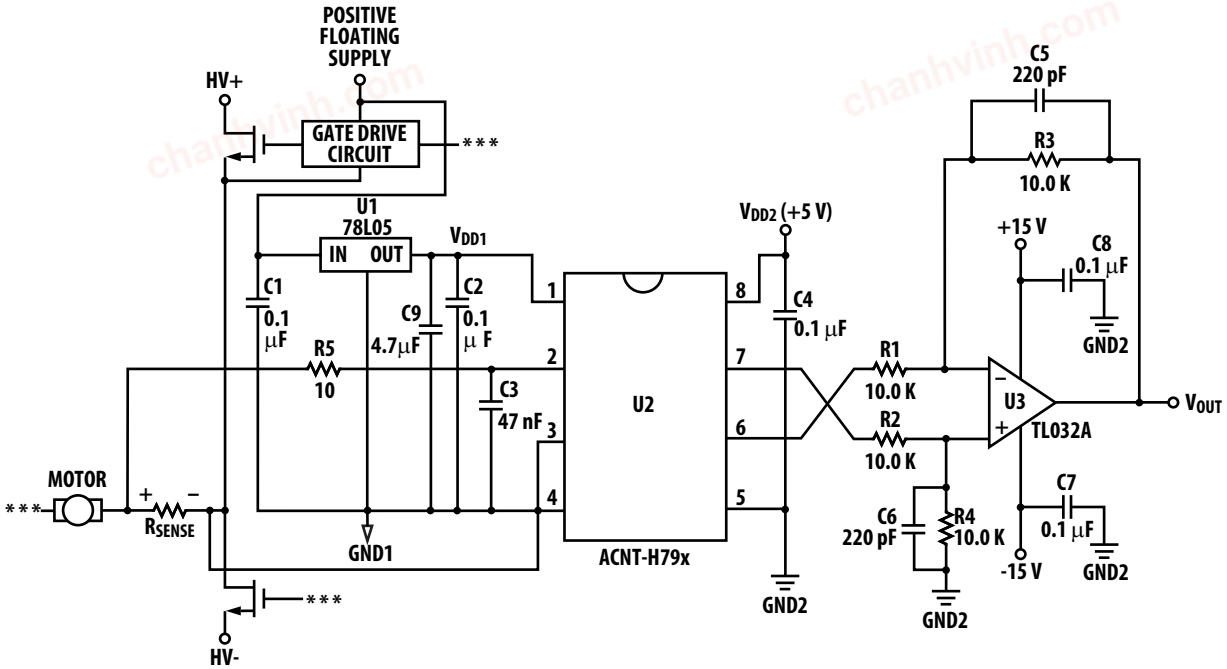
Application Information

Application Circuit

The typical application circuit is shown in Figure 21. A floating power supply (which in many applications could be the same supply that is used to drive the high-side power transistor) is regulated to 5V using a simple three-terminal voltage regulator (U1). The voltage from the current sensing resistor, or shunt (R_{SENSE}), is applied to the input of the ACNT-H79B/H79A/H790 through an RC anti-aliasing filter (R5 and C3). And finally, the differential output of the isolation amplifier is converted to a ground-referenced single-ended output voltage with a simple differential amplifier circuit (U3 and associated components). Although the application circuit is relatively simple, a few recommendations should be followed to ensure optimal performance.

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Figure 21: Typical Application Circuit for Motor Phase Current Sensing



Power Supplies and Bypassing

As mentioned above, an inexpensive 78L05 three-terminal regulator can be used to reduce the gate-drive power supply voltage to 5 V. To help attenuate high frequency power supply noise or ripple, a resistor or inductor can be used in series with the input of the regulator to form a low-pass filter with the regulator's input bypass capacitor.

The power supply for the isolation amplifier is most often obtained from the same supply used to power the power transistor gate drive circuit. If a dedicated supply is required, in many cases it is possible to add an additional winding on an existing transformer. Otherwise, some sort of simple isolated supply can be used, such as a line powered transformer or a high-frequency DC-DC converter.

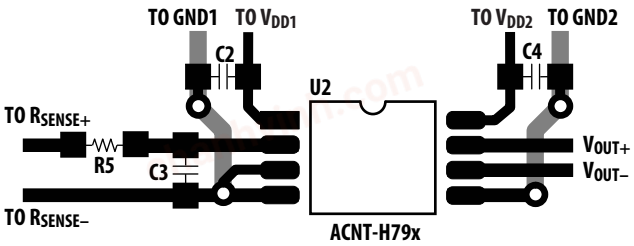
As shown in Figure 21, 0.1-µF bypass capacitors (C2, C4) should be located as close as possible to the pins of the isolation amplifier. The bypass capacitors are required because of the high-speed digital nature of the signals inside the isolation amplifier. A 47 nF bypass capacitor (C3) is also recommended at the input pins due to the switched-capacitor nature of the input circuit. The input bypass capacitor also forms part of the anti-aliasing filter, which is recommended to prevent high-frequency noise from aliasing down to lower frequencies and interfering with the input signal. The input filter also performs an important reliability function—it reduces transient spikes from ESD events flowing through the current sensing resistor.

PC Board Layout

The design of the printed circuit board (PCB) should follow good layout practices, such as keeping bypass capacitors close to the supply pins, keeping output signals away from input signals, the use of ground and power planes, etc. In addition, the layout of the PCB can also affect the isolation transient immunity (CMTI) of the ACNT-H79B/H79A/H790, due primarily to stray capacitive coupling between the input and the output circuits. To obtain optimal CMTI performance, the layout of the PC board should minimize any stray coupling by maintaining the maximum possible distance between the input and output sides of the circuit and ensuring that any ground or power plane on the PC board does not pass directly below or extend much wider than the body of the ACNT-H79B/H79A/H790. Figure 22 shows an example PCB layout.

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Figure 22: Example Printed Circuit Board Layout



Note: Drawing not to scale

Shunt Resistor Selection

The current sensing resistor should have low resistance (to minimize power dissipation), low inductance (to minimize di/dt induced voltage spikes which could adversely affect operation), and reasonable tolerance (to maintain overall circuit accuracy). Choosing a particular value for the resistor is usually a compromise between minimizing power dissipation and maximizing accuracy. Smaller sense resistance decreases power dissipation, while larger sense resistance can improve circuit accuracy by utilizing the full input range of the ACNT-H79B/H79A/H790.

The first step in selecting a sense resistor is determining how much current the resistor will be sensing. The graph in Figure 23 shows the RMS current in each phase of a three-phase induction motor as a function of average motor output power (in horsepower, hp) and motor drive supply voltage. The maximum value of the sense resistor is determined by the current being measured and the maximum recommended input voltage of the isolation amplifier. The maximum sense resistance can be calculated by taking the maximum recommended input voltage and dividing by the peak current that the sense resistor should see during normal operation. For example, if a motor will have a maximum RMS current of 10A and can experience up to 50% overloads during normal operation, then the peak current is 21.1A (=10 × 1.414 × 1.5). Assuming a maximum input voltage of 200 mV, the maximum value of sense resistance in this case would be about 10 mΩ.

The maximum average power dissipation in the sense resistor can also be easily calculated by multiplying the sense resistance times the square of the maximum RMS current, which is about 1W in the previous example. If the power dissipation in the sense resistor is too high, the resistance can be decreased below the maximum value to decrease power dissipation. The minimum value of the sense resistor is limited by precision and accuracy requirements of the design. As the resistance value is reduced, the output voltage across the resistor is also reduced, which means that the offset and noise, which are fixed, become a larger percentage of the signal amplitude. The selected value of the sense resistor will fall somewhere between the minimum and maximum values, depending on the particular requirements of a specific design.

When sensing currents large enough to cause significant heating of the sense resistor, the temperature coefficient (tempco) of the resistor can introduce nonlinearity due to the signal dependent temperature rise of the resistor. The effect increases as the resistor-to-ambient thermal resistance increases. This effect can be minimized by reducing the thermal resistance of the current sensing resistor or by using a resistor with a lower tempco. Lowering the thermal resistance can be accomplished by repositioning the current sensing resistor on the PC board, by using larger PC board traces to carry away more heat, or by using a heat sink.

For a two-terminal current sensing resistor, as the value of resistance decreases, the resistance of the leads become a significant percentage of the total resistance. This has two primary effects on resistor accuracy. First, the effective resistance of the sense resistor can become dependent on factors such as how long the leads are, how they are bent, how far they are inserted into the board, and how far solder wicks up the leads during assembly (these issues will be discussed in more detail shortly). Second, the leads are typically made from a material, such as copper, which has a much higher tempco than the material from which the resistive element itself is made, resulting in a higher tempco overall.

Both of these effects are eliminated when a four-terminal current sensing resistor is used. A four-terminal resistor has two additional terminals that are Kelvin connected directly across the resistive element itself; these two terminals are used to monitor the voltage across the resistive element while the other two terminals are used to carry the load current. Because of the Kelvin connection, any voltage drops across the leads carrying the load current should have no impact on the measured voltage.

When laying out a PC board for the current sensing resistors, a couple of points should be kept in mind. The Kelvin connections to the resistor should be brought together under the body of the resistor and then run very close to each other to the input of the ACNT-H79B/H79A/H790; this minimizes the loop area of the connection and

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reduces the possibility of stray magnetic fields from interfering with the measured signal. If the sense resistor is not located on the same PC board as the isolation amplifier circuit, a tightly twisted pair of wires can accomplish the same thing.

Also, multiple layers of the PC board can be used to increase current carrying capacity. Numerous plated-through vias should surround each non-Kelvin terminal of the sense resistor to help distribute the current between the layers of the PC board. The PC board should use 2 oz or 4 oz copper for the layers, resulting in a current carrying capacity in excess of 20A. Making the current carrying traces on the PC board fairly large can also improve the sense resistor's power dissipation capability by acting as a heat sink. Liberal use of vias where the load current enters and exits the PC board is also recommended.

Shunt Resistor Connections

The typical method for connecting the ACNT-H79B/H79A/H790 to the current sensing resistor is shown in Figure 21. V_{IN+} (pin 2) is connected to the positive terminal of the sense resistor, while V_{IN-} (pin 3) is shorted to GND1 (pin 4), with the power-supply return path functioning as the sense line to the negative terminal of the current sense resistor.

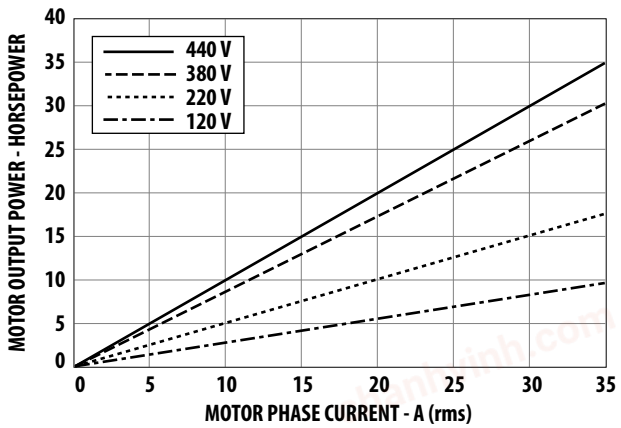
This allows a single pair of wires or PC board traces to connect the isolation amplifier circuit to the sense resistor. By referencing the input circuit to the negative side of the sense resistor, any load current induced noise transients on the resistor are seen as a common-mode signal and will not interfere with the current-sense signal. This is important because the large load currents flowing through the motor drive, along with the parasitic inductances inherent in the wiring of the circuit, can generate both noise spikes and offsets that are relatively large compared to the small voltages that are being measured across the current sensing resistor.

If the same power supply is used both for the gate drive circuit and for the current sensing circuit, it is very important that the connection from GND1 of the ACNT-H79B/H79A/H790 to the sense resistor be the only return path for supply current to the gate drive power supply in order to eliminate potential ground loop problems. The only direct connection between the ACNT-H79B/H79A/H790 circuit and the gate drive circuit should be the positive power supply line.

Differential Input Connection

The differential analog inputs of the ACNT-H79B/H79A/H790 are implemented with a fully-differential, switched-capacitor circuit. In the typical application circuit (Figure 21), the isolation amplifier is connected in a single-ended input mode. Given the fully differential input structure, a differential input connection method (balanced input mode as shown in Figure 24) is recommended to achieve better performance. The input currents created by the switching actions on both of the pins are balanced on the filter resistors and cancelled out each other. Any noise induced on one pin will be coupled to the other pin by the capacitor C and creates only common mode noise that is rejected by the device. Typical value for Ra and Rb is 10Ω and 22 nF for C.

Figure 23: Motor Output Horsepower vs. Motor Phase Current and Supply Voltage



Output Side

The op-amp used in the external post-amplifier circuit should be of sufficiently high precision so that it does not contribute a significant amount of offset or offset drift relative to the contribution from the isolation amplifier. Generally, op-amps with bipolar input stages exhibit better offset performance than op-amps with JFET or MOSFET input stages.

In addition, the op-amp should also have enough bandwidth and slew rate so that it does not adversely affect the response speed of the overall circuit. The post-amplifier circuit includes a pair of capacitors (C5 and C6) that form a

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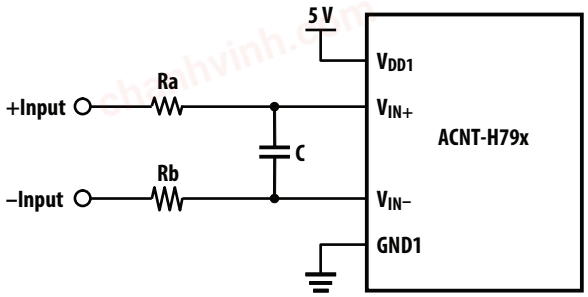
single-pole low-pass filter; these capacitors allow the bandwidth of the post-amp to be adjusted independently of the gain and are useful for reducing the output noise from the isolation amplifier.

The gain-setting resistors in the post-amp should have a tolerance of 1% or better to ensure adequate CMRR and adequate gain tolerance for the overall circuit. Resistor networks can be used that have much better ratio tolerances than can be achieved using discrete resistors. A resistor network also reduces the total number of components for the circuit as well as the required board space.

Voltage Sensing

The ACNT-H79B/H79A/H790 can also be used to isolate signals with amplitudes larger than its recommended input range with the use of a resistive voltage divider at its input. The only restrictions are that the impedance of the divider be relatively small (less than 1 kΩ) so that the input resistance (27 kΩ) and input bias current (0.1 µA) do not affect the accuracy of the measurement. An input bypass capacitor is still required, although the 10Ω series damping resistor is not (the resistance of the voltage divider provides the same function). The low-pass filter formed by the divider resistance and the input bypass capacitor may limit the achievable bandwidth.

Figure 24: Simplified Differential Input Connection Diagram



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